A Peak Capacitor Current Pulse-Train Controlled Buck Converter with Fast Transient Response and a Wide Load Range

Jin Sha, Duo Xu, Yiming Chen, Jianping Xu and Barry W. Williams

***Abstract*—It is known that ripple-based control of a switching dc-dc converter benefits from a faster transient response than a conventional PWM control switching dc-dc converter. However, ripple-based control switching dc-dc converters may suffer from fast-scale oscillation. In order to achieve fast transient response and ensure stable operation of a switching dc-dc converter over a wide load range, based on a conventional pulse train control technique, a peak capacitor current pulse train (PCC-PT) control technique is proposed in this paper. With a buck converter as an example, the operating modes, steady-state performance and transient respond performance of a PCC-PT controlled buck converter are presented and assessed. To eliminate fast-scale oscillation, circuit and control parameter design consideration are given. An accurate discrete iteration model of a PCC-PT controlled buck converter is established, based on which, the effects of circuit parameters on stability of converter operating in a DCM mode, mixed DCM-CCM mode, and CCM mode are studied. Simulation and experimental results are presented to verify the analysis results.**

***Index Terms*— Capacitor current feedback, pulse train control, switching DC-DC converter, wide load range**

I. Introduction

SWITCHING DC-DC converters have been widely used in portable electronic devices, such as mobile phones, note-books and tablet PC. In some applications, the load power of switching dc-dc converters varies widely and rapidly [1-3]. Various control techniques, such as V^2 control, constant-on-time (COT) control or constant-off-time (CFT) control, and pulse train (PT) control [4-10], have been reported to improve transient response speed of switching dc-dc converters. These control techniques, called 'ripple-based control' techniques [11], regulate the output voltage of switching DC-DC converters by using output voltage ripple. Ripple-based control techniques do not require an error amplifier and its associated compensation circuit, thus, they benefit from simple control circuit design, fast transient response, and high reliability.

However, ripple-based control techniques of switching DC-DC converters usually suffer from fast-scale instability [12]. The V^2 controlled buck converter has the sub-harmonic instability issue when the duty ratio $D < ½$ [5]. COT and CFT controlled buck converter become unstable and suffer fast-scale oscillation when the time constant of output capacitor $R_{ESR}C$, where R_{ESR} is equivalent series resistance (ESR) of output capacitor C, is smaller than $½\tau_{on}$ and $½\tau_{off}$ (τ_{on} and τ_{off} are on and off times of the COT and CFT control respectively) [6, 7, 10]. For a PT controlled buck converter, the ESR also significant affects control performance, with fast-scale oscillation when the ESR is small, but disappears when the ESR is large enough [13].

Studies of critical ESR have been recently reported, which provide guidelines for the design of ripple-based controlled switching DC-DC converters [4, 10, 13]. However, critical ESR is derived based on ideal conditions. The fast-scale oscillation phenomenon may still occur even when critical ESR is satisfied. In addition, larger output capacitor ESR produces larger output voltage ripple. To avoid such fast-scale oscillation, some control techniques, such as COT control with added inductor current ramp [7] and PT control with inductor current ripple injection feedback (ICRIF) [13], have been proposed. These improved control techniques combine inductor current with output voltage ripple for output voltage regulation. In this paper, based on a conventional PT control technique [14], a peak capacitor-current PT (PCC-PT) control technique is proposed. Fast-scale oscillation in the conventional PT controlled CCM buck converter is eliminated in the PCC-PT controlled buck converter. Moreover, the PCC-PT controlled buck converter benefits from simple design, fast transient response, small output voltage ripple, and a wide load range.

This paper is organized as follows. The control principle and corresponding operating modes of the PCC-PT control technique are presented in Section II. Section III addresses stability analysis of the PCC-PT controlled buck converter. The converter's output voltage variation, output power range and line and load regulation are studied, and circuit parameter

This work was supported by the National Natural Science Foundation of China under Grant (51177140), the Fundamental Research Funds for the Central Universities under grant (2682013ZT20) and National Natural Science Foundation of China under Grant (51407054).

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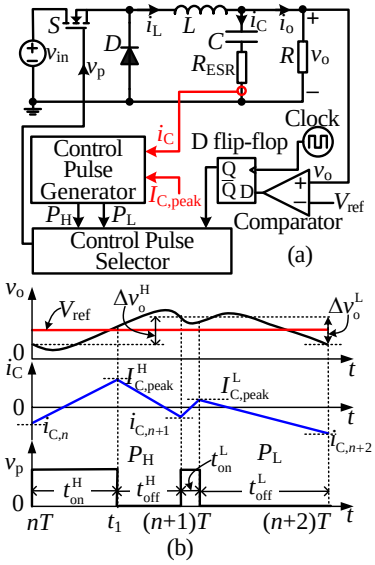

Fig. 1. PCC-PT controlled buck converter: (a) schematic diagram and (b) time domain waveforms of PCC-PT controlled buck converter.

design consideration is presented. A discrete iteration model of the buck converter is established in Section IV. Upon this model, circuit parameter effects on stability performance of PCC-PT controlled buck converter operating in DCM mode, mixed DCM-CCM mode, and CCM mode are studied. In Section V, steady-state and transient response simulation and experimental results are presented to verify the analysis.

II. PCC-PT Control Technique

A. PCC-PT Control Technique Principle

Fig. 1 shows the schematic diagram and time domain waveforms of the PCC-PT controlled buck converter. At the start of each switching cycle, in the outer control loop, output voltage v_o is sampled and compared with reference voltage V_{ref} to determine whether high power control pulse P_H or low power control pulse P_L should be selected as the active control pulse in this switching cycle. As shown in Fig. 1(b), at $t=nT$, v_o is lower than V_{ref}, P_H is selected as the active control pulse to increase the output voltage. Similarly, at $t=(nT+1)$, v_o is higher than V_{ref}, P_L is selected as the active control pulse to decrease the output voltage.

In the inner control loop, capacitor current i_C is sensed and compared with reference peak current $I_{C,peak}$ to determine when to turn off switch S. For buck converter, $i_L=i_C+i_o$, where output current $i_o=v_o/R$ can be considered as a constant in steady-state. Thus, the inductor current ripple flows through the output capacitor, *i.e.*, i_C is in phase with i_L. At the start of a switching cycle, switch S is turned on, i_C increases, and S is turned off when i_C increases to $I_{C,peak}$, as shown in Fig. 1(b). For high power control pulse P_H, $I_{C,peak}=I_{C,peak}^H$, and for low power control pulse P_L, $I_{C,peak}=I_{C,peak}^L$, that is

$$I_{C,peak}=\begin{cases} I_{C,peak}^H & \text{if } v_o \le V_{ref} \\ I_{C,peak}^L & \text{if } v_o > V_{ref} \end{cases} \tag{1}$$

where $I_{C,peak}^H > I_{C,peak}^L$.

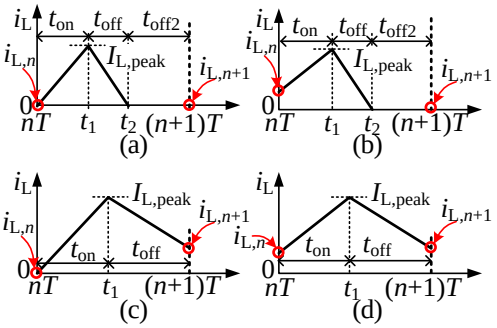

Fig. 2. Different inductor current modes: (a) $i_{L,n}=0$ and $i_{L,n+1}=0$, (b) $i_{L,n}\neq 0$ and $i_{L,n+1}=0$, (c) $i_{L,n}=0$ and $i_{L,n+1}\neq 0$, and (d) $i_{L,n}\neq 0$ and $i_{L,n+1}\neq 0$.

PCC-PT control and conventional PT control have the same outer control loop [8, 9], but a different inner control loop, where PCC-PT controller utilizes capacitor current as the feedback signal to control the turn-off of pulses P_H and P_L.

In one switching cycle, the output voltage variation is $\Delta v_o=v_o((n+1)T)-v_o(nT)$. According to the principle of PCC-PT control technique, control pulse P_H should be applied to make the output voltage increase, that is, output voltage variation $\Delta v_o^H>0$. Similarly, control pulse P_L should be applied to make the output voltage decrease, that is, output voltage variation $\Delta v_o^L<0$. PCC-PT operates in period-n states with control pulses P_H and P_L in n successive switching cycles constituting a controlled pulse repetition cycle, as its output voltage variation may only vary between the discrete states Δv_o^H and Δv_o^L, rather than period-1 in the PWM switching converter [9]. Let the number of P_H and P_L in a control pulse repetition cycle be denoted as μ_H and μ_L respectively, then μ_H and μ_L satisfy $\mu_H/\mu_L=\Delta v_o^L/\Delta v_o^H$ [15], and the control pulse repetition cycle period T_r is $T_r=(\mu_H+\mu_L)T$.

B. Operating Modes of PCC-PT Controlled Buck Converter

Let $i_{L,n}$ and $i_{L,n+1}$ denote the inductor currents at the beginning of the n^{th} and $(n+1)^{th}$ switching cycle respectively. For inductor current i_L of the PCC-PT controlled buck converter, there are four inductor current operation cases, as shown in Fig. 2,

Case 1: $i_{L,n}=0$ and $i_{L,n+1}=0$, as shown in Fig. 2(a);
Case 2: $i_{L,n}\neq 0$ and $i_{L,n+1}=0$, as shown in Fig. 2(b);
Case 3: $i_{L,n}=0$ and $i_{L,n+1}\neq 0$, as shown in Fig. 2(c);
Case 4: $i_{L,n}\neq 0$ and $i_{L,n+1}\neq 0$, as shown in Fig. 2(d).

Assume output voltage ripple is small enough to be ignored, that is, the output voltage can be considered as constant in a switching cycle. As $i_L=i_C+i_o$ and $i_o=v_o/R$, the peak inductor current $I_{L,peak}=I_{C,peak}+v_o/R$.

If $t_{on}+t_{off}<T$, $i_{L,n+1}=0$, which corresponds to Case 1 and 2, as shown in Fig. 2(a) and (b). In Cases 1 and 2, $i_L(t)$ in the n^{th} switching cycle are

$$i_L(t)=i_{L,n}+\frac{(v_{in}-v_o)t}{L}, \quad [nT, nT+t_{on}] \tag{2a}$$

$$i_L(t)=I_{L,peak}-\frac{v_o}{L}t, \quad [nT+t_{on}, nT+t_{on}+t_{off}] \tag{2b}$$

$$i_{\mathrm{L}}(t)=0, \quad [nT+t_{\mathrm{on}}+t_{\mathrm{off}},(n+1)T] \tag{2c}$$

As $i_{\mathrm{L}}(nT+t_{\mathrm{on}}) = I_{\mathrm{L,\,peak}}$, from (2), the time durations t_{on}, t_{off} and t_{off2} of the PCC-PT controlled buck converter in Fig. 2(a) and (b) can be calculated as

$$t_{\mathrm{on}}=\frac{L(I_{\mathrm{C,\,peak}}-i_{\mathrm{L},\,n}+v_{\mathrm{o}}/R)}{v_{\mathrm{in}}-v_{\mathrm{o}}}, \tag{3a}$$

$$t_{\mathrm{off}}=\frac{L(I_{\mathrm{C,\,peak}}+v_{\mathrm{o}}/R)}{v_{\mathrm{o}}}, \tag{3b}$$

$$t_{\mathrm{off2}}=T-t_{\mathrm{on}}-t_{\mathrm{off}}. \tag{3c}$$

If t_{on} and t_{off} in Eq. (3) satisfy $t_{\mathrm{on}}+t_{\mathrm{off}}>T$, $i_{\mathrm{L},\,n+1}>0$, which corresponds to Cases 3 and 4, as shown in Fig. 2(c) and (d). In Cases 3 and 4, in the n^{th} switching cycle, $i_{\mathrm{L}}(t)$ and the time durations t_{on} and t_{off} should be rewritten as

$$i_{\mathrm{L}}(t)=i_{\mathrm{L},\,n}+\frac{v_{\mathrm{in}}-v_{\mathrm{o}}}{L}t, \qquad [nT,nT+t_{\mathrm{on}}] \tag{4a}$$

$$i_{\mathrm{L}}(t)=(I_{\mathrm{C,\,peak}}+\frac{v_{\mathrm{o}}}{R})-\frac{v_{\mathrm{o}}}{L}t, \qquad [nT+t_{\mathrm{on}},(n+1)T] \tag{4b}$$

$$t_{\mathrm{on}}=\frac{L(-i_{\mathrm{L},\,n}+I_{\mathrm{C,\,peak}}+v_{\mathrm{o}}/R)}{v_{\mathrm{in}}-v_{\mathrm{o}}}, \tag{4c}$$

$$t_{\mathrm{off}}=T-t_{\mathrm{on}}. \tag{4d}$$

When t_{on} and t_{off} in Eq. (3) satisfy $t_{\mathrm{on}}+t_{\mathrm{off}}=T$, $i_{\mathrm{L},\,n+1}=0$, there exists an inductor current boundary. From (3a) and (3b), such an inductor current boundary can be written as

$$\frac{L(I_{\mathrm{C,\,peak}}-i_{\mathrm{L},\,n}+v_{\mathrm{o}}/R)}{v_{\mathrm{in}}-v_{\mathrm{o}}}+\frac{L(I_{\mathrm{C,\,peak}}+v_{\mathrm{o}}/R)}{v_{\mathrm{o}}}-T=0 \tag{5a}$$

Let R in (5a) be variable, and the right part of the equation in (5a) be $f(R)$, then

$$\begin{aligned} f(R)&=(RLI_{\mathrm{C,\,peak}}+Lv_{\mathrm{o}}-Rv_{\mathrm{o}}T)v_{\mathrm{in}}\\ &\quad+(Rv_{\mathrm{o}}T-Li_{\mathrm{L},\,n})v_{\mathrm{o}}\\ &=0 \end{aligned} \tag{5b}$$

where $f(R) = f_{\mathrm{L}}(R)$ for the low power control pulse P_{L}, and $f(R) = f_{\mathrm{H}}(R)$ for the high power control pulse P_{H}. When $f(R)<0$, $i_{\mathrm{L},n+1}<0$; and when $f(R)>0$, $i_{\mathrm{L},\,n+1}>0$.

Thus, in a switching cycle, when $i_{\mathrm{L},\,n}=0$, $f(R)<0$, which corresponding to Case 1 as shown in Fig. 2(a), means the converter operates in a DCM in this switching cycle; when $i_{\mathrm{L},n}\neq0$, $f(R)>0$, which corresponding to Case 4, as shown in Fig. 2(d), means the converter operates in a CCM in this switching cycle.

As the PCC-PT controlled buck converter operates in period-n states rather than period-1, that is, control pulses P_{H} and P_{L} in n successive switching cycles constituting a control pulse repetition cycle, rather than period-1 in a PWM switching converter [9]. In a control pulse repetition cycle, the PCC-PT controlled buck converter may operate in DCM, CCM and mixed DCM-CCM, herein mixed DCM-CCM is defined as the operating mode when both CCM and DCM exists in a control pulse repetition cycle. In mixed DCM-CCM, $i_{\mathrm{L},n}\neq0$, $f(R)<0$ (corresponding to Case 2 as shown in Fig. 2(b)) and $i_{\mathrm{L},\,n}=0$, $f(R)>0$ (corresponding to Case 3 as shown in Fig. 2(c)) may occur. Thus, different from a PWM controlled buck converter which has two operating modes: DCM and CCM, the PCC-PT controlled buck converter has three operating modes: DCM, CCM and mixed DCM-CCM. When all switching cycles of a control pulse repetition cycle satisfy $i_{\mathrm{L},n}=0$, $f_{\mathrm{L}}(R)<0$ and $f_{\mathrm{H}}(R)<0$, the converter operates in DCM; when all switching cycles of a control pulse repetition cycle satisfy $i_{\mathrm{L},\,n}\neq0$, $f_{\mathrm{L}}(R)>0$ and $f_{\mathrm{H}}(R)>0$, the converter operates in CCM; and when none of these conditions are satisfied, the converter operates in mixed DCM-CCM.

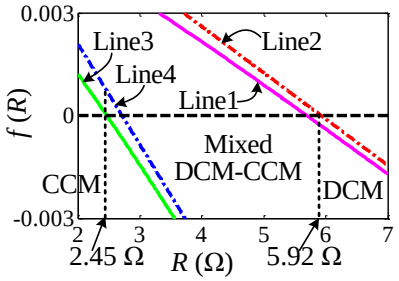

Fig. 3. The operating modes and corresponding borders of PCC-PT controlled buck converter.

Fig. 3 shows the distributions of CCM, DCM and mixed DCM-CCM operating modes with the main circuit parameters as v_{in}=20V, v_{ref}=5V, L=80μH, C=440μF, and the controller parameters of the PCC-PT as T=50μs, $I^{\mathrm{H}}_{\mathrm{peak}}$=1.5A, $I^{\mathrm{L}}_{\mathrm{peak}}$=0.5A. In Fig. 3, Line 1 is $i_{\mathrm{L},\,n}\neq0$, $f_{\mathrm{H}}(R)$; Line 2 is $i_{\mathrm{L},\,n}=0$, $f_{\mathrm{H}}(R)$; Line 3 is $i_{\mathrm{L},\,n}\neq0$, $f_{\mathrm{L}}(R)$; and Line 4 is $i_{\mathrm{L},\,n}=0$, $f_{\mathrm{L}}(R)$.

From Fig. 3, when R < 2.45 Ω, both lines 1 and 3 are above zero, that is, $i_{\mathrm{L},\,n}\neq0$, $f_{\mathrm{H}}(R)>0$ and $f_{\mathrm{L}}(R)>0$, the converter operates in CCM. When R > 5.92 Ω, both lines 2 and 4 are below zero, that is, $i_{\mathrm{L},\,n}=0$, $f_{\mathrm{H}}(R)<0$ and $f_{\mathrm{L}}(R)<0$, the converter operates in DCM. When 2.45 Ω < R < 5.92 Ω, the converter operates in mixed DCM-CCM.

III. Steady-State Analysis

A. Output Voltage Variations of the PCC-PT Controlled Buck Converter

From the discussion in Section II, the PCC-PT controlled buck converter has four inductor current operation cases, the only difference between Case 1 (Case 3) and Case 2 (Case 4) is inductor current $i_{\mathrm{L},\,n}$ at the beginning of switching cycle. When $i_{\mathrm{L},\,n}=0$, Case 1 is the same as Case 2, and Case 3 is the same as Case 4. Thus, for convenience, only Cases 2 and 4 are analyzed in this section, and Cases 1 and 3 can be analyzed by considering $i_{\mathrm{L},\,n}=0$.

1) Output Voltage Variation of Case 2 (Case 1)

As $i_{\mathrm{C}}=i_{\mathrm{L}}-i_{\mathrm{o}}$, from (2)

$$i_{\mathrm{C}}(t)=i_{\mathrm{C},\,n}+\frac{v_{\mathrm{in}}-v_{\mathrm{o}}}{L}t \qquad [nT,nT+t_{\mathrm{on}}], \tag{6a}$$

$$i_{\mathrm{C}}(t)=I_{\mathrm{C,\,peak}}-\frac{v_{\mathrm{o}}}{L}t \qquad [nT+t_{\mathrm{on}},nT+t_{\mathrm{on}}+t_{\mathrm{off}}] \tag{6b}$$

$$i_{\mathrm{C}}(t)=-\frac{v_{\mathrm{o}}}{R} \quad [nT+t_{\mathrm{on}}+t_{\mathrm{off}},(n+1)T] \tag{6c}$$

where $i_{\mathrm{C},\,n}=i_{\mathrm{L},\,n}-v_{\mathrm{o}}/R$ is the capacitor current at the beginning

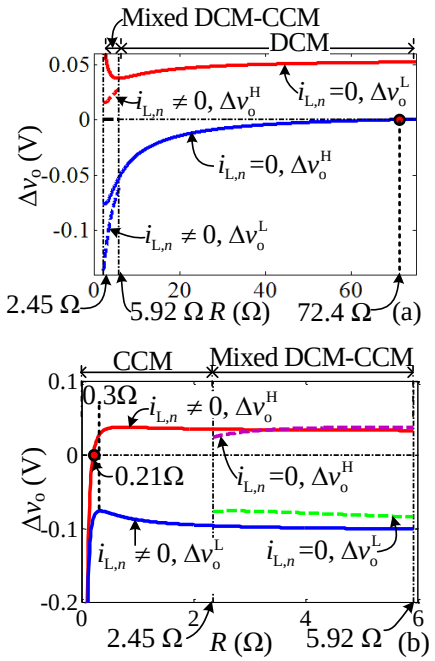

Fig. 4. Output voltage variations of the PCC-PT controlled buck converter: (a) DCM and mixed DCM-CCM and (b) mixed DCM-CCM and CCM.

of a switching cycle. Thus when $i_{L,n} = 0$, $i_{C,n} = -v_o/R$.

From (3) and (6), output voltage variation Δv_o within one switching cycle is

$$\Delta v_o = \frac{1}{C}\int_{(n+1)T}^{nT} i_C dt \qquad (7)$$
$$= \frac{L(v_{in} I_{C,peak} - v_o i_{C,n}^2)}{2Cv_o(v_{in} - v_o)} + \frac{L(v_{in} I_{C,peak} - v_o i_{C,n})}{RC(v_{in} - v_o)} + \frac{v_o(L - 2RT)}{2R^2C}$$

where $\Delta v_o = \Delta v_o^H$ for P_H and $\Delta v_o = \Delta v_o^L$ for P_L.

With the same circuit parameters as given in section II, Fig.4(a) shows output voltage variations Δv_o^H and Δv_o^L of the PCC-PT controlled DCM buck converter, where solid lines show Δv_o^H and Δv_o^L for Case 1 when the converter operates in DCM, that is, $i_{C,n} = -v_o/R$, and dotted lines show Δv_o^H and Δv_o^L for Case 2 when the converter operates in mixed DCM-CCM, that is, $i_{C,n} \neq -v_o/R$.

For 2.45 Ω<R<5.92 Ω, the converter operates in mixed DCM-CCM, $\Delta v_o^H > 0$ and $\Delta v_o^L < 0$ are always satisfied as shown in Fig. 4(a). For R > 5.92 Ω, the converter operates in DCM, Δv_o^H and Δv_o^L increase with increased R, $\Delta v_o^H > 0$ and $\Delta v_o^L < 0$ until R increases to R = 72.4 Ω. For R > 72.4 Ω, $\Delta v_o^L > 0$, that is, even if P_L is selected as the active control pulse, the output voltage cannot decrease, and the PCC-PT controller cannot regulate the converter any more.

2) Output Voltage Variation of Case 4 (Case 3)

From (4) and (6), output voltage variation Δv_o within one switching cycle is

$$\Delta v_o = -\frac{Lv_{in}(I_{C,peak} - i_{C,n})^2}{2C(v_{in} - v_o)^2} + \frac{(v_{in} I_{C,peak} - v_o i_{C,n})T}{C(v_{in} - v_o)} - \frac{v_o T^2}{2LC} \qquad (8)$$

With the same circuit parameters as given in section II, output voltage variations Δv_o^H and Δv_o^L of the PCC-PT controlled buck converter operating in CCM and mixed DCM-CCM are shown in Fig. 4(b). In Fig. 4(b), solid lines show Δv_o^H and Δv_o^L for Case 4 when the converter operates in CCM, that is, $i_{C,n} \neq -v_o/R$, and dotted lines show Δv_o^H and Δv_o^L for Case 3 when the converter operates in mixed DCM-CCM, that is, $i_{C,n} = -v_o/R$.

When 2.45 Ω<R<5.92 Ω, the converter operates in mixed DCM-CCM, $\Delta v_o^H > 0$ and $\Delta v_o^L < 0$ are always satisfied as shown in Fig. 4(b). When R < 2.45 Ω, the converter operates in CCM, with the decrease of R, Δv_o^H decreases and Δv_o^L increases slightly. When R<0.3 Ω, both Δv_o^H and Δv_o^L decrease dramatically. When R<0.21 Ω, $\Delta v_o^H < 0$, that is, even if P_H is selected as the active control pulse, the output voltage cannot increase, and the PCC-PT controller cannot regulate the converter any more.

B. Circuit Parameter Design of the PCC-PT Controlled Buck Converter

From the previous discussion, for the PCC-PT controlled buck converter, when a high power control pulse P_H is applied, the output voltage variation may be lower than zero, that is, $\Delta v_o^H > 0$ is not satisfied, and when a low power control pulse P_L is applied, the output voltage variation may be larger than zero, that is, $\Delta v_o^L < 0$ is not satisfied. Thus, $\Delta v_o^H > 0$ and $\Delta v_o^L < 0$ should be considered in the parameter design. The design of control parameters follows.

For a light load condition, from (7), as $i_{C,n} = -v_o/R$, $\Delta v_o^L < 0$ and $\Delta v_o^H > 0$:

$$I_{C,peak}^L < \sqrt{\frac{2(v_{in} - v_o)v_o^2 T}{RLv_{in}}} - \frac{v_o}{R} \qquad (9a)$$

$$I_{C,peak}^H > \sqrt{\frac{2(v_{in} - v_o)v_o^2 T}{RLv_{in}}} - \frac{v_o}{R} \qquad (9b)$$

For a heavy load condition, from (8), as $\Delta v_o^L < 0$ and $\Delta v_o^H > 0$:

$$I_{C,peak}^2 - 2(i_{C,n} + \frac{(v_{in} - v_o)T}{L})I_{C,peak} + [i_{C,n}^2 + \frac{2v_o(v_{in} - v_o)T}{Lv_{in}} i_{C,n} + \frac{v_o(v_{in} - v_o)^2 T^2}{L^2 v_{in}}] < 0 \qquad (10a)$$

which can be rewritten as

$$I_{C,peak} < i_{C,n} + \frac{(v_{in} - v_o)T}{L}[1 + \sqrt{1 + \frac{2Li_{C,n} - v_o T}{v_{in} T}}] \qquad (10b)$$

To ensure $\Delta v_o^H > 0$, $I_{C,peak}$ should be smaller than the minimum of the right part of (10b), which occurs when $i_{C,n} = -v_o/R$

$$I_{C,peak} < -\frac{v_o}{R} + \frac{(v_{in} - v_o)T}{L}[1 + \sqrt{1 - \frac{2Lv_o + Rv_o T}{Rv_{in} T}}] \qquad (10c)$$

Thus, (9) and (10c) should be satisfied for the parameter design of the PCC-PT controlled buck converter.

C. Output Power Range

Base on the previous discussion, under a light load condition, the PCC-PT controlled buck converter operates in DCM. With increased load power, converter goes into mixed DCM-CCM, and then goes into CCM. Thus, the minimum and maximum load powers $P_{\min}$ and $P_{\max}$ occur in DCM and CCM, respectively.

When the converter operates in DCM, the power from the input power source is completely transferred to the load within one switching cycle. Assuming the converter is lossless, then the power delivered from input power source to the load in one switching cycle is given by [9]

$$P_{\mathrm{DCM}} = v_{\mathrm{in}} I_{\mathrm{ave}} = \frac{L v_{\mathrm{in}}}{2(v_{\mathrm{in}} - v_{\mathrm{o}})T}(I_{\mathrm{C,\,peak}} + \frac{v_{\mathrm{o}}}{R})^2 \tag{11}$$

where I_{ave} is the average current flowing through S in a switching cycle. When P_{H} is selected, $P_{\mathrm{DCM}} = P_{\mathrm{DCM}}^{\mathrm{H}}$; and when P_{L} is selected, $P_{\mathrm{DCM}} = P_{\mathrm{DCM}}^{\mathrm{L}}$, that is

$$P_{\mathrm{DCM}} = \begin{cases} P_{\mathrm{DCM}}^{\mathrm{H}}, & \text{if } v_{\mathrm{o}} \le V_{\mathrm{ref}} \\ P_{\mathrm{DCM}}^{\mathrm{L}}, & \text{if } v_{\mathrm{o}} > V_{\mathrm{ref}} \end{cases}.$$

From (11), P_{DCM} varies with the variation of load resistance R, rather than fixed as with the conventional PT controlled buck converter [9]. For the PCC-PT controlled buck converter, $P_{\mathrm{DCM}}^{\mathrm{H}}$ and $P_{\mathrm{DCM}}^{\mathrm{L}}$ should satisfy

$$\begin{aligned} P_{\mathrm{DCM}}^{\mathrm{H}} &> P_{\mathrm{o}} = \frac{v_{\mathrm{o}}^2}{R}, \\ P_{\mathrm{DCM}}^{\mathrm{L}} &\le P_{\mathrm{o}} = \frac{v_{\mathrm{o}}^2}{R}. \end{aligned} \tag{12}$$

where P_{o} is load power.

When the converter operates in CCM, the inductor may store or release energy in one switching cycle, thus load power not only transferred from input power but also from the energy stored in the inductor. The input power P_{in} in one switching cycle is

$$P_{\mathrm{in}} = v_{\mathrm{in}} I_{\mathrm{ave}} = \frac{v_{\mathrm{in}} t_{\mathrm{on}}}{2T}(i_{\mathrm{L},\,n} + I_{\mathrm{C,\,peak}} + \frac{v_{\mathrm{o}}}{R})^2 \tag{13}$$

From (2) and (4), $i_{\mathrm{L},\,n+1}$ can be obtained as $i_{\mathrm{L},\,n+1}=I_{\mathrm{C,\,peak}}+v_{\mathrm{o}}/R - v_{\mathrm{o}}(T-t_{\mathrm{on}})/L$. The energy variation of the inductor ΔE_{L} is

$$\Delta E_{\mathrm{L}} = \tfrac{1}{2} L (i_{\mathrm{L},\,n+1}^2 - i_{\mathrm{L},\,n}^2) \tag{14}$$

Then the power delivered from the input power source to the load in one switching cycle is

$$P_{\mathrm{CCM}} = P_{\mathrm{in}} - \frac{\Delta E_{\mathrm{L}}}{T} \tag{15}$$

With the same circuit parameters as given in section II, $P_{\mathrm{DCM}}^{\mathrm{H}}$, $P_{\mathrm{DCM}}^{\mathrm{L}}$, $P_{\mathrm{CCM}}^{\mathrm{H}}$, $P_{\mathrm{CCM}}^{\mathrm{L}}$ and P_{o} with respect to R are shown in Fig. 5. As shown in Fig. 5(a), all decrease with increased R. For $R >$ 5.92 Ω, the converter operates in DCM, as shown in Fig. 5(a). For $R >$ 72.4 Ω, $P_{\mathrm{DCM}}^{\mathrm{L}} > P_{\mathrm{o}}$, that is, when P_{L} is selected as a control pulse, more power than load power P_{o} is delivered from input power source to the load, which increases the output voltage rather than decreasing it. Thus, as with conventional PT control, P_{L} of the PCC-PT controller determines the minimum load power $P_{\min}$, which can be calculated from (12) as

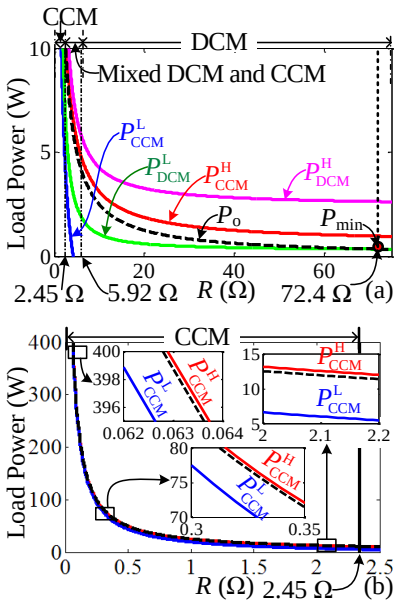

Fig. 5 The output powers of PCC-PT controlled buck converter: (a) the output power range of PCC-PT controlled buck converter and (b) zoom in view of (a).

$$\begin{aligned} P_{\min} = {} & \frac{v_{\mathrm{o}}^2 (v_{\mathrm{in}} - v_{\mathrm{o}})T}{L v_{\mathrm{in}}} - v_{\mathrm{o}} I_{\mathrm{C,\,peak}} \\ & + v_{\mathrm{o}} \sqrt{(\frac{v_{\mathrm{o}}^2 (v_{\mathrm{in}} - v_{\mathrm{o}})T}{L v_{\mathrm{in}}} - 2 v_{\mathrm{o}} I_{\mathrm{C,\,peak}}) \frac{(v_{\mathrm{in}} - v_{\mathrm{o}})T}{L v_{\mathrm{in}}}} \end{aligned} \tag{16}$$

For 5.92 Ω < R < 72.4 Ω, as shown in Fig. 5(a), $P_{\mathrm{DCM}}^{\mathrm{L}} < P_{\mathrm{o}} < P_{\mathrm{DCM}}^{\mathrm{H}}$, that is, in this condition, when P_{H} is selected, more power than load power P_{o} is delivered from the input power source to the load, which makes output voltage increase; and when P_{L} is selected, less power than load power P_{o} is delivered from the input power source to the load, which decreases the output voltage. Thus, PCC-PT control can adjust the buck converter output voltage by selecting P_{H} or P_{L}.

For 2.45 Ω < R < 5.92 Ω, the converter operates in mixed DCM-CCM, as shown in Fig. 5(a), both $P_{\mathrm{DCM}}^{\mathrm{L}} < P_{\mathrm{o}} < P_{\mathrm{DCM}}^{\mathrm{H}}$ and $P_{\mathrm{CCM}}^{\mathrm{L}} < P_{\mathrm{o}} < P_{\mathrm{CCM}}^{\mathrm{H}}$ are satisfied, that is, the PCC-PT controller can control the buck converter.

For $R <$ 2.45 Ω, the converter operates in CCM, as shown in Fig. 5(b), it always has $P_{\mathrm{CCM}}^{\mathrm{L}} < P_{\mathrm{o}} < P_{\mathrm{CCM}}^{\mathrm{H}}$, thus, the converter can be controlled at heavy load conditions. Different from conventional PT control, the maximum load power of the PCC-PT controlled buck converter does not only depend on P_{H}, the output power can be high if the input power source can provide sufficient power.

From this analysis, as power delivered from the input power source to the load in one switching cycle increases (decreases) with the increase (decrease) of load power, the PCC-PT controlled buck converter can operate under a wide load power range.

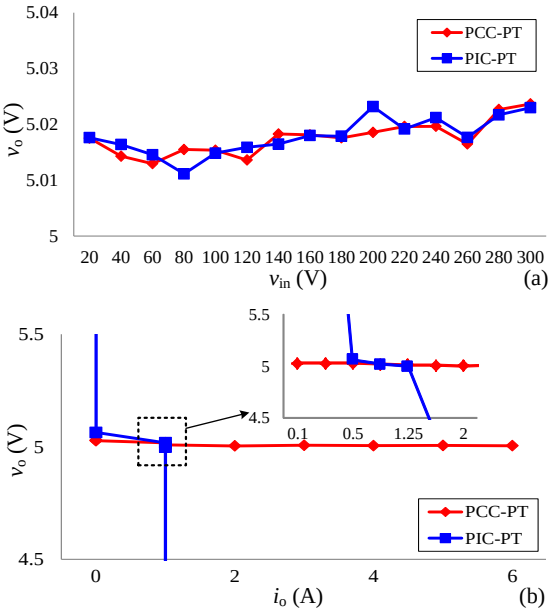

Fig. 6. Circuit performances: (a) line regulations of PCC-PT and PIC-PT controlled buck converters, and (b) load regulations of PCC-PT and PIC-PT controlled buck converters.

D. Line and Load Regulation

With the same circuit parameters as given in section II, line regulations of PCC-PT controlled buck converter and peak inductor current PT (PIC-PT) controlled buck converter are shown in Fig. 6 (a). The line regulations of PCC-PT and PIC-PT controlled buck converters for input voltage varying from 20 V to 300 V are 0.103% and 0.112%, respectively. PCC-PT and PIC-PT controlled buck converters have the similar line regulations.

Load regulations of PCC-PT and PIC-PT controlled buck converters with v_{in}=20 V are shown in Fig. 6 (b), note that the x-axis in zoom-in window is at uneven increments. The load regulation of PCC-PT controlled buck converter from a minimum output current (0.1 A) to 6 A is 0.437%. The load regulation of PIC-PT controlled buck converter from a minimum output current (0.5 A) to a maximum output voltage current (1.25 A) is 1.305%. From Fig. 6 (b), PCC-PT controlled buck converter has wider load range and better load regulation than that of PIC-PT controlled buck converter.

IV. Discrete Iteration Model

To verify the analysis in Section III, a discrete iteration model of the PCC-PT controlled buck converter, with output capacitor ESR considered, is established in this section.

A. Operation States

For the PCC-PT controlled buck converter, when switch S is turned on and diode D is turned off, the converter operates in switch state 1. During this switch state, the inductor current i_L and capacitor voltage v_C are

$$\begin{cases} L\dfrac{di_L(t)}{dt} = v_{in} - \dfrac{RR_{ESR}}{R+R_{ESR}}i_L(t) - \dfrac{R}{R+R_{ESR}}v_C(t), \\ C\dfrac{dv_C(t)}{dt} = \dfrac{R}{R+R_{ESR}}i_L(t) - \dfrac{1}{R+R_{ESR}}v_C(t). \end{cases} \tag{17}$$

which can be solved as

$$\begin{cases} v_C(t) = e^{-\alpha t}[(v_{C,n} - v_{in})\cos(\omega t) + k_1\sin(\omega t)] + v_{in}, \\ i_L(t) = e^{-\alpha t}[(i_{L,n} - \dfrac{v_{in}}{R})\cos(\omega t) + k_2\sin(\omega t)] + \dfrac{v_{in}}{R}. \end{cases} \tag{18}$$

where α, k_1 and k_2 are

$$\alpha = \frac{RR_{ESR}C + L}{2(R+R_{ESR})LC},\ \omega = \sqrt{\frac{R}{(R+R_{ESR})LC} - \alpha^2},$$

$$k_1 = \frac{R}{(R+R_{ESR})C\omega}i_{L,n} + \frac{RR_{ESR}C - L}{2(R+R_{ESR})LC\omega}v_{C,n} - \frac{\alpha}{\omega}v_{in},$$

$$k_2 = \frac{(L - RR_{ESR}C)}{2(R+R_{ESR})LC\omega}i_{L,n} - \frac{R}{(R+R_{ESR})L\omega}v_{C,n} + \frac{R-\alpha L}{RL\omega}v_{in}.$$

As $i_C(t_{on}) = I_{C,peak}$, from (18), the time duration t_{on} of switch state 1 is

$$t_{on} = \frac{-\beta_2 + \sqrt{\beta_2^2 - 2\beta_1\beta_3}}{\beta_1} \tag{19}$$

where

$$\beta_1 = 2(\alpha^2 - \frac{R}{(R+R_{ESR})LC})(Ri_{L,n} - v_{C,n}) - \alpha(Rk_2 - k_1)\omega,$$

$$\beta_2 = (Rk_2 - k_1)\omega - \alpha(Ri_{L,n} - v_{C,n}), \text{ and}$$

$$\beta_3 = (Ri_{L,n} - v_{C,n}) - (R+R_{ESR})I_{C,peak}.$$

After time duration t_{on}, switch S is turned off and diode D is turned on, the converter operates in switch state 2. During this switch state, the inductor current i_L and capacitor voltage v_C are

$$\begin{cases} L\dfrac{di_L(t)}{dt} = -\dfrac{R}{R+R_{ESR}}v_C(t) - \dfrac{RR_{ESR}}{R+R_{ESR}}i_L(t), \\ C\dfrac{dv_C(t)}{dt} = \dfrac{R}{R+R_{ESR}}i_L(t) - \dfrac{1}{R+R_{ESR}}v_C(t). \end{cases} \tag{20}$$

which can be solved as

$$\begin{cases} v_C(t) = e^{-\alpha t}[v_C(t_{on})\cos(\omega t) + k_3\sin(\omega t)], \\ i_L(t) = e^{-\alpha t}[i_L(t_{on})\cos(\omega t) + k_4\sin(\omega t)]. \end{cases} \tag{21}$$

where $i_L(t_{on}) = I_{L,peak}$ and $v_C(t_{on})$ are the initial conditions of switch state 2, $v_C(t_{on})$ can be obtained from (18), and k_3 and k_4 in (21) are

$$k_3 = \frac{R}{(R+R_{ESR})C\omega}i_L(t_{on}) + \frac{RR_{ESR}C - L}{2(R+R_{ESR})LC\omega}v_C(t_{on}),$$

$$k_4 = -\frac{RR_{ESR}C - L}{2(R+R_{ESR})LC\omega}i_L(t_{on}) - \frac{R}{(R+R_{ESR})L\omega}v_C(t_{on}).$$

In switch state 2, i_L decreases. When i_L decreases to zero before the end of the switching cycle, the converter operates in DCM, otherwise, it operates in CCM.

When the PCC-PT controlled buck converter operates in CCM, time duration t_{off} in this switch state is

$$t_{off} = T - t_{on} \tag{22}$$

When converter operates in DCM, as $i_L(t_2) = 0$, where $t_2 = t_{on}+t_{off}$ from (21), the time duration t_{off} in this switch state is

$$t_{off} = \frac{1}{\omega}\arctan\frac{RI_{C,peak} - v_C(t_{on})}{k_3 - Rk_4} \tag{23}$$

After i_L decreases to zero, it remains at zero, and both switch S and diode D are turned off. The converter operates in switch state 3. During this switch state, the inductor current i_L and

capacitor voltage v_C are

$$\begin{cases} L\dfrac{di_L(t)}{dt}=0, \\ C\dfrac{dv_C(t)}{dt}=-\dfrac{1}{R+R_{ESR}}v_C(t). \end{cases} \tag{24}$$

which can be solved as

$$\begin{cases} v_C(t)=e^{-\frac{t}{(R+R_{ESR})C}}v_C(t_2), \\ i_L(t)=0. \end{cases} \tag{25}$$

where $v_C(t_2)$ is the initial condition of switch state 3, which can be obtained from (21). The time duration of switch state 3 is $t_{off2} = T-t_{on}-t_{off}$.

B. Discrete Iteration Model

From (18), (19), (21) and (22), the discrete iteration model of the PCC-PT controlled CCM buck converter can be derived as

$$\begin{cases} v_{C,n+1}=e^{-\alpha T}[(v_{C,n}-v_{in})\cos\omega T+k_1\sin\omega T] \\ \quad +v_{in}[\cos(\omega t_{off})+\dfrac{\alpha}{\omega}\sin(\omega t_{off})]e^{-\alpha t_{off}}, \\ i_{L,n+1}=e^{-\alpha T}[(i_{L,n}-\dfrac{v_{in}}{R})\cos\omega T+k_2\sin\omega T] \\ \quad +\dfrac{v_{in}}{R}[\cos(\omega t_{off})+\dfrac{\alpha L-R}{\omega L}\sin(\omega t_{off})]e^{-\alpha t_{off}}. \end{cases} \tag{26}$$

From (18), (19), (21), (23) and (25), the discrete iteration model of the PCC-PT controlled DCM buck converter is

$$\begin{cases} v_{C,n+1}=e^{-\alpha(t_{on}+t_{off}+\frac{t_{off1}}{(R+R_{ESR})C})}[(v_{C,n}-v_{in})\cos\omega(t_{on}+t_{off}) \\ \quad +k_1\sin\omega(t_{on}+t_{off})] \\ \quad +v_{in}[\cos(\omega t_{off})+\dfrac{\alpha}{\omega}\sin(\omega t_{off})]e^{-\frac{t_{off1}}{(R+R_{ESR})C}-\alpha t_{off}}, \\ i_{L,n+1}=0. \end{cases} \tag{27}$$

C. Effects of Circuit Parameters on the Stability of the PCC-PT Controlled Buck Converter

Based on discrete iteration models (26) and (27), the effect of load resistance on the steady-state performance of the PCC-PT controlled buck converter is studied in this section.

Fig. 7(a) shows the bifurcation diagrams of the output voltage v_o with load resistance R as the bifurcation parameter. As shown in Fig. 7(a), with increased R, the converter goes from multi-periodicities to period-1 at R =72.4 Ω, which is consistent with the analysis in Section III.

Fig. 7(b) shows the bifurcation diagrams of inductor current i_L with load resistance R as the bifurcation parameter. Fig. 7(b) shows the operating modes of the PCC-PT controlled buck converter: for R < 2.36 Ω, inductor current orbits are always higher than zero, that is, the converter operates in CCM; for 2.36 Ω < R < 5.69 Ω, there exists i_L =0, that is, the converter operates in mixed DCM-CCM; and for R > 5.69 Ω, all inductor current orbits decrease to zero and remain at zero, that is, the converter operates in DCM. The small difference between the ranges of these three operating modes and the ranges calculated in Section III is caused by the ESR and the accuracy of model.

Fig. 7(c) shows that for all R, the maximal Lyapunov exponent is less than zero, which illustrates that the converter is stable.

Fig. 7(d)-(g) are the zoom-in views of Fig. 7 (a), where some special periodicities are presented. Fig. 7 (d) and (e) show bifurcation diagrams when the converter operates in DCM. The converter operates in period-3 with control pulse combination $1P_H$-$2P_L$ for 14.93 Ω < R < 15.08 Ω, and operates in period-2 with control pulse combination $1P_H$-$1P_L$ for 8.62 Ω < R < 8.81 Ω. Fig. 7 (f) shows bifurcation diagrams when the converter operates in mixed DCM-CCM. Wth the decrease of R, the converter operates in period-8 with control pulse combination $5P_H$-$3P_L$, period-3 with control pulse combination $2P_H$-$1P_L$, and period-7 with control pulse combination $5P_H$-$2P_L$. The same control pulse combination, such as period-3 with control pulse combination $2P_H$-$1P_L$, can exist in different operating modes of the PCC-PT controlled buck converter. Fig. 7 (g) shows bifurcation diagrams when the converter operates in CCM. The converter operates in period-4 with control pulse combination $3P_H$-$1P_L$ for 1.12 Ω<R<1.61 Ω. From Fig. 7(d)-(g), with increased R, the ratio between the number of high power control pulse μ_H and low power control pulse μ_L increases.

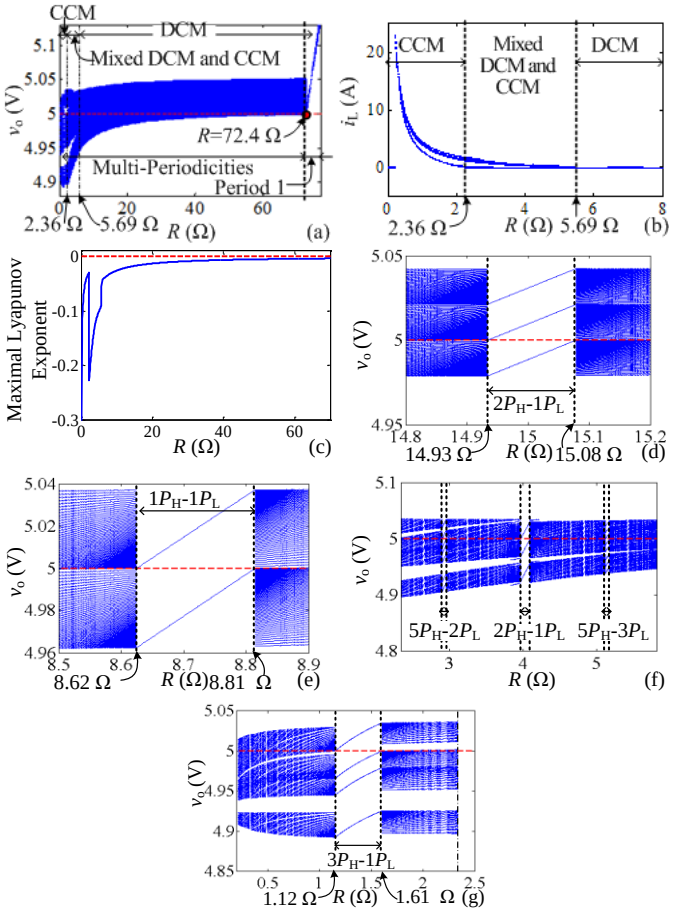

Fig. 7. Effects of circuit parameters on the steady-state performance of PCC-PT controlled buck converter: (a) bifurcation diagram of v_o with the increase of R, (b) bifurcation diagram of i_L with the increase of R, (c) maximal Lyapunov exponent with the increase of R, (d) zoom in view of (a), (e) zoom in view of (a), (f) zoom in view of (a), and (g) zoom in view of (a).

V. Simulation and Experimental Results

Fig. 8 shows simulation results of the PCC-PT controlled buck converter with the same circuit parameters as given in section II for different load resistances. Fig. 8(a) shows waveforms of output voltage v_o, capacitor current i_C, inductor

current i_L and switch driving voltage v_p for R = 75 Ω. The load is too light to be controlled by the PCC-PT controller, v_o is always higher than reference voltage V_{ref}, low power control pulse P_L is thus continuously applied as the control pulse, and the converter operates in period-1 with the control pulse repetition cycle consisting of only P_L.

Fig. 8(b) and (c) show the waveforms for R = 15 Ω and R = 8.7 Ω. The converter operates in DCM. For R = 15 Ω, the converter operates in period-3 with control pulse combination $1P_H$-$2P_L$. For R = 8.7 Ω, converter operates in period-2 with control pulse combination $1P_H$-$1P_L$.

Fig. 8(d)-(f) show the waveforms for R = 5.1 Ω, R = 4 Ω and R=2.9 Ω. The converter operates in mixed DCM-CCM. For R=5.1 Ω, the converter operates in period-8 consisting of $5P_H$ and $3P_L$, and the control pulse combination is $2(2P_H$-$1P_L)$ -$1(1P_H$-$1P_L)$. For R=4 Ω, the converter operates in period-3 with control pulse combination $2P_H$-$1P_L$. For R=2.9 Ω, the converter operates in period-7 which consists of 5_H and $2P_L$, and the control pulse combination is $1(3P_H$-$1P_L)$-$1(2P_H$-$1P_L)$.

Fig. 8(g)-(h) show the waveforms for R = 1.5 Ω and R = 0.3 Ω. The converter operates in CCM. For R = 1.5 Ω,the converter operates in period-4 with control pulse combination $3P_H$-$1P_L$. For R = 0.3 Ω, the converter operates in period-3 with control pulse combination $2P_H$-$1P_L$. Simulation results of Fig. 8 are consistent with the theoretical analysis results.

Fig. 9 shows transient response of PCC-PT controlled buck converter under step load current variation from 5 A to 1 A and from 1 A to 5 A, respectively. As shown in Fig. 9(a), when load current i_o step decreases at time t=10.5 ms, as inductor current i_L can not change immediately, and because of i_C=i_L−i_o, output capacitor current i_C abruptly jumps to 3.548 A which is larger than $I^{H}_{C,\,peak}$, the switch S is then turned off immediately. Three low power control pulses are selected as active control pulses to decrease the output voltage. After four switching cycles, the converter goes into a steady-state. The transient time is 4 switching cycles (200 μs) and the output voltage overshoot is 0.213 V (4.26%).

When load current i_o step increases at time t=10.5 ms as shown in Fig. 9(b), i_C decreases to −4.695A. Two high power control pulses are selected as active control pulses to increase the output voltage. After 2 switching cycles, the converter goes into a steady-state. The transient time is 2 switching cycles (100 μs) and the output voltage sag is 0.135 V (2.7%).

By using the same circuit parameters, experimental results of the PCC-PT controlled buck converters are shown in Fig. 10. For R = 15 Ω, the converter operates in period-3 with control pulse combination $1P_H$-$2P_L$, as shown in Fig. 10(a). For R = 8.7 Ω, the converter operates in period-2 with control pulse combination $1P_H$-$1P_L$, as shown in Fig. 10(b). As shown in Figs. 10(a) and (b), the converter operates in DCM.

Fig.10(c) shows that for R = 4 Ω, the converter operates in mixed DCM-CCM and in period-3 with control pulse combination $2P_H$-$1P_L$. Fig.10(d) shows that for R = 0.3 Ω, the converter operates in CCM and in period-3 with control pulse combination $2P_H$-$1P_L$. These experimental results verify the theoretical analysis and simulation results.

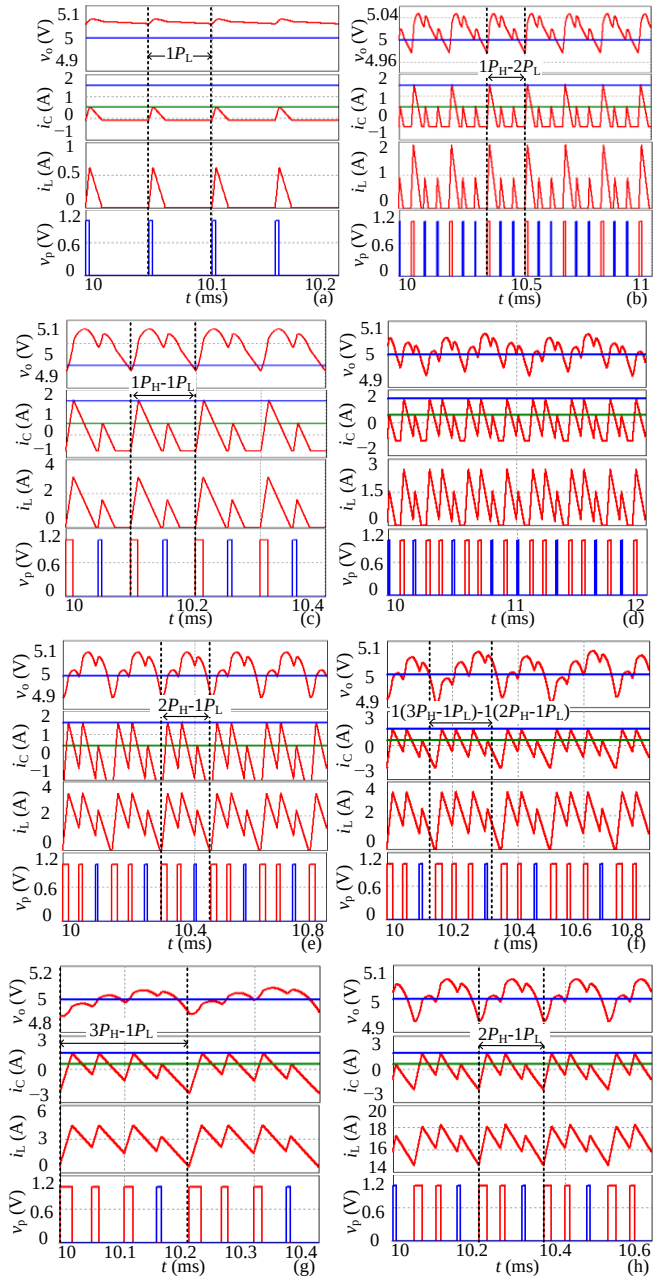

Fig. 8. Simulation result: (a) DCM, R = 75 Ω, (b) DCM, R = 15 Ω, (c) DCM, R = 8.7 Ω, (d) mixed DCM-CCM, R = 5.1 Ω, (e) mixed DCM-CCM, R = 4 Ω, (f) mixed DCM-CCM, R = 2.9 Ω, (g) CCM, R = 1.5 Ω, and (h) CCM, R = 0.3 Ω.

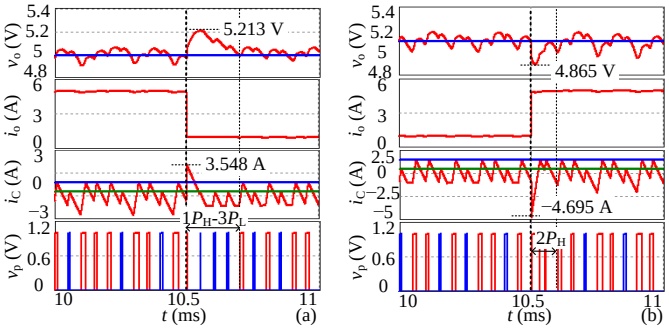

Fig. 9. Transient response simulation results: (a) load current step decreases from 5A to 1 A, and (b) load current step increases from 1 A to 5 A.

TABLE I. COMPARISON TABLE WITH THE PREVIOUS WORKS

	Proposed in this paper	Ref.[4]	Ref. [14,15]	Ref. [16]	Ref. [17]	Ref. [18]
Control technique	PCC-PT	Digital enhanced V^2-type COT	PIC-PT	PCM-BF	IPR	VCM-PT
Input voltage (v_{in})	20 V	12 V	20 V	20 V	15 V	12 V
Output voltage (v_o)	5 V	1.2 V	5 V	6 V	5 V	5 V
Output capacitor (C)	440 µF	1600 µF	440 µF	1880 µF	800 µF	470 µF
Switching frequency (f)	20 kHz	15 MHz (Maximum frequency)	20 kHz	16.7-66.7 kHz	20 kHz	40-125 kHz
Load range (P_o)	0.35-119.05 W		2.5-6.25 W	6-12 W	0.5-4.9 W	6-13 W
Operating modes	DCM, Mixed DCM-CCM, CCM	CCM	DCM	DCM	DCM	CCM
Line regulation	0.103 % (20 V-300 V)		0.112 % (20 V-300 V)			
Load regulation	0.437 % (0.1 A-6 A)		1.305 % (0.5 A-1.25 A)		1.386% (0.08-0.8 A)	
Load transient	1 -5 A	6 -18 A	1 -2 A	1-2 A	0.08-0.8 A	
Recovery time (T_R)	50-250 µs	38 µs	1.8 ms	125 µs	50 µs	
Switching cycle number for recovery	2-5 Switching cycles	About 50 Switching cycles	9 Switching cycles	2-8 Switching cycles	1 Switching cycles	

Abbreviations: PCM-BF — Peak current mode bifrequency control;
ICRIF — Inductor current ripple injection feedback circuit;
IPR — Improved pulse regulation;
VCM-PT — Valley current mode pulse train.

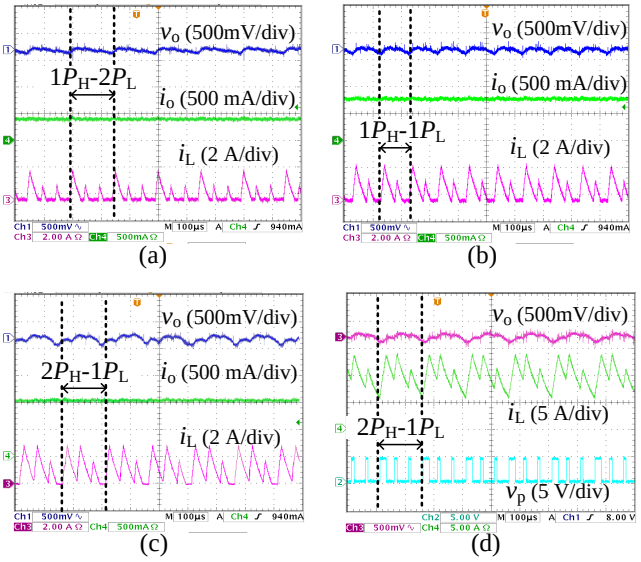

Fig. 10. Experimental results: (a) DCM, R = 15 Ω, (b) DCM, R = 8.7 Ω, (c) mixed DCM-CCM, R = 4 Ω, and (d) CCM, R = 0.3 Ω.

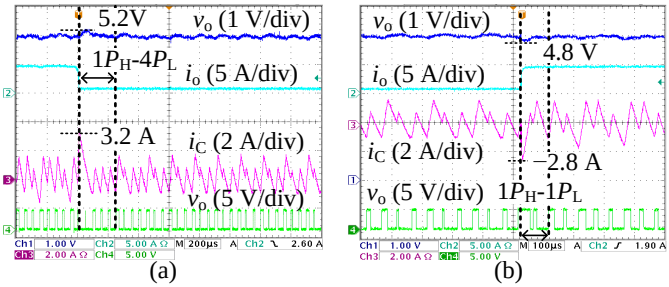

Fig. 11. Transient response experimental results of PT and PCC-PT controlled buck converter: (a) load current step decreases from 5A to 1 A, and (b) load current step increases from 1 A to 5 A.

Fig. 11 shows the transient response experimental results of conventional PT and PCC-PT controlled buck converter under step load variation from 5 A to 1 A and from 1 A to 5 A, respectively. As shown in Fig. 11(a), when load current i_o step decreases from 5 A to 1 A, output capacitor current i_C increases to 3.2 A, which is larger than $I^H_{C,\,peak}$, the switch S is then turned off immediately. Four low power control pulses are selected as active control pulses to decrease the output voltage. After five switching cycles, the converter goes into a steady-state. The transient response time is 5 switching cycles and the output voltage overshoot is about 0.2 V (4%). As shown in Fig. 11(b), when load current i_o step increases from 1 A to 5 A, i_C decreases to −2.8 A. One low power control pulse and one high power control pulse are selected as active control pulses to increase the output voltage. After 2 switching cycles, the converter goes into a steady-state. The transient response time is 2 switching cycles and the output voltage sag is 0.2 V (4%), approximately.

Moreover, the comparisons with the previous ripple-based control techniques are shown in Table I. From Table I, because of different switching frequences f, the comparative study of transient responses of different control techniques is not obvious by comparing recovery times T_R. Thus, the switching cycle numbers of transient process, which reduces the effect of switching frequence, are considered to evaluate the transient performance. For PCC-PT controlled buck converter, only 2-5 switching cycles are required to get into steady state, which is less than the other control techniques. Moreover, the transient response of PCC-PT controlled converters can be improved by increasing switching frequency.

VI. Conclusion

In this paper, based on a discrete control technique, conventional PT control, for switching dc-dc converters, a PCC-PT control technique for the buck converter is proposed and analysed. Different from PT control, PCC-PT control uses peak capacitor current as a feedback control variable to generate high power control pulse P_H and low power control pulse P_L. The output voltage variations, Δv_o^H and Δv_o^L, of the

PCC-PT controlled buck converter with output load variation are studied; from which, control parameter design is presented. From theory and simulation analysis, within a wide load range, $\Delta v_o^H > 0$ and $\Delta v_o^L < 0$ can always be satisfied, that is, the fast-scale oscillation in a conventional PT controlled buck converter can be eliminated. In order to better understand the characteristics of the PCC-PT control buck converter, an accurate discrete iteration model of the PCC-PT controlled buck converter was established. From this model, the effects of circuit parameters on stability performance of the PCC-PT controlled buck converter operating in DCM, mixed DCM-CCM, and CCM are studied. The presented simulation and experimental results verify the analysis.

REFERENCES

[1] C. Ji-Soo, O. Hyoung-Seok, J. Young-Hyun, and K. Bai-Sun, "Fast Output Voltage-Regulated PWM Buck Converter With an Adaptive Ramp Amplitude Control," *IEEE Trans. Circuits Syst. II: Express Briefs,* vol. 60, pp. 712-716, Oct. 2013.

[2] Y. Bing, L. Xin-Quan, W. Hong-Yi, and S. Ling-Feng, "High-Efficient Hybrid Buck Converter With Switch-on-Demand Modulation and Switch Size Control for Wide-Load Low-Ripple Applications," *IEEE Trans. Microw. Theory Tech.,* vol. 61, pp. 3329-3338, Sep. 2013.

[3] S. Maity and Y. Suraj, "A fixed frequency dual-mode DC-DC buck converter with fast-transient response and high efficiency over a wide load range," in *2013 Twenty-Eighth Annual IEEE Applied Power Electronics Conference and Exposition (APEC)*, 2013, pp. 415-420.

[4] K. Cheng, F. Yu, F. C. Lee, and P. Mattavelli, "Digital Enhanced V2-Type Constant On-Time Control Using Inductor Current Ramp Estimation for a Buck Converter With Low-ESR Capacitors," *IEEE Trans. Power Electron.,* vol. 28, pp. 1241-1252, March 2013.

[5] G. Zhou, J. Xu, and J. Wang, "Constant-Frequency Peak-Ripple-Based Control of Buck Converter in CCM: Review, Unification, and Duality," *IEEE Trans. Ind. Electron.*, vol. 61, pp. 1280-1291, March 2014.

[6] T. Qian, W. Wu, and W. Zhu, "Effect of Combined Output Capacitors for Stability of Buck Converters With Constant On-Time Control," *IEEE Trans. Ind. Electron.*, vol. 60, pp. 5585-5592, Dec. 2013.

[7] T. Qian, "Study of Subharmonic Oscillation Mechanism and Effect of Circuit Propagation Delay for Buck Converters With Constant On-Time Control," *IEEE Trans. Circuits Syst. I: Regular Papers*, vol. 60, pp. 788-795, March 2013.

[8] M. Ferdowsi, A. Emadi, M. Telefus, and C. Davis, "Pulse regulation control technique for flyback converter," *IEEE Trans. Power Electron.*, vol. 20, pp. 798-805, Aug. 2005.

[9] S. Jin, X. Jianping, B. Bocheng, and Y. Tiesheng, "Effects of Circuit Parameters on Dynamics of Current-Mode-Pulse-Train-Controlled Buck Converter," *IEEE Trans. Ind. Electron.,* vol. 61, pp. 1562-1573, March 2014.

[10] J. Wang, B. Bao, J. Xu, G. Zhou, and W. Hu, "Dynamical Effects of Equivalent Series Resistance of Output Capacitor in Constant On-Time Controlled Buck Converter," *IEEE Trans. Ind. Electron.*, vol. 60, pp. 1759-1768, May 2013.

[11] J. Sun, "Characterization and performance comparison of ripple-based control for voltage regulator modules," *IEEE Trans. Power Electron.*, vol. 21, pp. 346-353, March 2006.

[12] R. Redl and S. Jian, "Ripple-Based Control of Switching Regulators--An Overview," *IEEE Trans. Power Electron.*, vol. 24, pp. 2669-2680, Dec. 2009.

[13] J. Wang, J. Xu, G. Zhou, and B. Bao, "Pulse-Train-Controlled CCM Buck Converter With Small ESR Output-Capacitor," *IEEE Trans. Ind. Electron.*, vol. 60, pp. 5875-5881, Dec. 2013.

[14] J. Sha, J. Xu, L. Xu, and S. Zhong, "Capacitor current feedback pulse train control technique for switching DC-DC converters," *Electron. Lett.*, vol. 50, pp. 1088-1090, July 2014.

[15] J. Sha, J. Xu, S. Zhong, S. Liu, and L. Xu, "Control Pulse Combination-Based Analysis of Pulse Train Controlled DCM Switching DC-DC Converters," *IEEE Trans. Ind. Electron.*, vol. 62, pp. 246-255, Jan. 2015.

[16] J. Wang, and J. Xu, "Peak Current Mode Bifrequency Control Technique for Switching DC–DC Converters in DCM With Fast Transient Response and Low EMI," *IEEE Trans. Power Electron.*, vol. 27, pp. 1876-1884, Apr. 2012.

[17] M. Qin, and J. Xu, "Multiduty Ratio Modulation Technique for Switching DC–DC Converters Operating in Discontinuous Conduction Mode, " *IEEE Trans. Ind. Electron.*, vol. 60, pp. 1819 - 1830, Oct. 2013.

[18] J. Sha, J. Xu, S. Zhong, and S. Liu, "Valley current mode pulse train control technique for switching DC-DC converters," *Electron. Lett.*, vol. 50, pp. 311 - 313, Feb. 2014.

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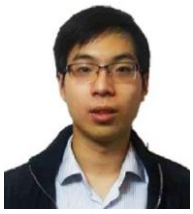

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