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A Peak Capacitor Current Pulse-Train Controlled Buck Converter with Fast Transient Response and a Wide Load Range

Jin Sha, Duo Xu, Yiming Chen, Jianping Xu and Barry W. Williams

Abstract—It is known that ripple-based control of a switching dc-dc converter benefits from a faster transient response than a conventional PWM control switching dc-dc converter. However, ripple-based control switching dc-dc converters may suffer from fast-scale oscillation. In order to achieve fast transient response and ensure stable operation of a switching dc-dc converter over a wide load range, based on a conventional pulse train control technique, a peak capacitor current pulse train (PCC-PT) control technique is proposed in this paper. With a buck converter as an example, the operating modes, steady-state performance and transient response performance of a PCC-PT controlled buck converter are presented and assessed. To eliminate fast-scale oscillation, circuit and control parameter design consideration are given. An accurate discrete iteration model of a PCC-PT controlled buck converter is established, based on which, the effects of circuit parameters on stability of converter operating in a DCM mode, mixed DCM-CCM mode, and CCM mode are studied. Simulation and experimental results are presented to verify the analysis results.

Index Terms—Capacitor current feedback, pulse train control, switching DC-DC converter, wide load range

I. INTRODUCTION

Switching DC-DC converters have been widely used in portable electronic devices, such as mobile phones, notebooks and tablet PC. In some applications, the load power of switching dc-dc converters varies widely and rapidly [1-3]. Various control techniques, such as V^2 control, constant-on-time (COT) control or constant-off-time (CFT) control, and pulse train (PT) control [4-10], have been reported to improve transient response speed of switching dc-dc converters. These control techniques, called ‘ripple-based control’ techniques [11], regulate the output voltage of switching DC-DC converters by using output voltage ripple. Ripple-based control techniques do not require an error amplifier and its associated compensation circuit, thus, they benefit from simple control circuit design, fast transient response, and high reliability.

However, ripple-based control techniques of switching DC-DC converters usually suffer from fast-scale instability [12]. The V^2 controlled buck converter has the sub-harmonic instability issue when the duty ratio D < ½ [5]. COT and CFT controlled buck converter become unstable and suffer fast-scale oscillation when the time constant of output capacitor R_C * C, where R_C is equivalent series resistance (ESR) of output capacitor C, is smaller than ½ * r_on and ½ * r_off (r_on and r_off are on and off times of the COT and CFT control respectively) [6, 7, 10]. For a PT controlled buck converter, the ESR also significant affects control performance, with fast-scale oscillation when the ESR is small, but disappears when the ESR is large enough [13].

Studies of critical ESR have been recently reported, which provide guidelines for the design of ripple-based controlled switching DC-DC converters [4, 10, 13]. However, critical ESR is derived based on ideal conditions. The fast-scale oscillation phenomenon may still occur even when critical ESR is satisfied. In addition, larger output capacitor ESR produces larger output voltage ripple. To avoid such fast-scale oscillation, some control techniques, such as COT control with added inductor current ramp [7] and PT control with inductor current ripple injection feedback (ICRIF) [13], have been proposed. These improved control techniques combine inductor current with output voltage ripple for output voltage regulation. In this paper, based on a conventional PT control technique [14], a peak capacitor-current PT (PCC-PT) control technique is proposed. Fast-scale oscillation in the conventional PT controlled CCM buck converter is eliminated in the PCC-PT controlled buck converter. Moreover, the PCC-PT controlled buck converter benefits from simple design, fast transient response, small output voltage ripple, and a wide load range.

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A discrete iteration model of the buck converter is established in Section IV. Upon this model, circuit parameter effects on stability performance of PCC-PT controlled buck converter operating in DCM mode, mixed DCM-CCM mode, and CCM mode are studied. In Section V, steady-state and transient response simulation and experimental results are presented to verify the analysis.

II. PCC-PT CONTROL TECHNIQUE

A. PCC-PT Control Technique Principle

Fig. 1 shows the schematic diagram and time domain waveforms of the PCC-PT controlled buck converter. At the start of each switching cycle, in the outer control loop, output voltage $v_o$ is sampled and compared with reference voltage $V_{ref}$ to determine whether high power control pulse $P_{H}$ or low power control pulse $P_{L}$ should be selected as the active control pulse in this switching cycle. As shown in Fig. 1(b), at $t=nT$, $v_o$ is lower than $V_{ref}$, $P_{H}$ is selected as the active control pulse to increase the output voltage. Similarly, at $t=(nT+1)$, $v_o$ is higher than $V_{ref}$, $P_{L}$ is selected as the active control pulse to decrease the output voltage.

In the inner control loop, capacitor current $i_C$ is sensed and compared with reference peak current $I_{C\text{-peak}}$ to determine when to turn off switch $S$. For buck converter, $i_C=i_L+i_o$, where output current $i_o=\frac{v_o}{R}$ can be considered as a constant in a steady-state. Thus, the inductor current ripple flows through the output capacitor, i.e., $i_C$ is in phase with $i_L$. At the start of a switching cycle, switch $S$ is turned on, $i_C$ increases, and $S$ is turned off when $i_c$ increases to $I_{C\text{-peak}}$ as shown in Fig. 1(b). For high power control pulse $P_{H}$, $I_{C\text{-peak}}^{H}=I_{C\text{-peak}}^{L}$, and for low power control pulse $P_{L}$, $I_{C\text{-peak}}^{H}=I_{C\text{-peak}}^{L}$, that is

$$I_{C\text{-peak}}^{H}= \begin{cases} I_{C\text{-peak}}^{L} & \text{if } \Delta v_o \leq V_{ref} \\ I_{C\text{-peak}}^{L} & \text{if } \Delta v_o > V_{ref} \end{cases}$$

where $I_{C\text{-peak}}^{H} > I_{C\text{-peak}}^{L}$.

Fig. 1: PCC-PT controlled buck converter: (a) schematic diagram and (b) time domain waveforms of PCC-PT controlled buck converter.

PCC-PT control and conventional PT control have the same outer control loop [8, 9], but a different inner control loop, where PCC-PT controller utilizes capacitor current as the feedback signal to control the turn-off of pulses $P_H$ and $P_L$.

In one switching cycle, the output voltage variation is $\Delta v_o=v_o((n+1)T)-v_o(nT)$. According to the principle of PCC-PT control technique, control pulse $P_H$ should be applied to make the output voltage increase, that is, output voltage variation $\Delta v_o>0$. Similarly, control pulse $P_L$ should be applied to make the output voltage decrease, that is, output voltage variation $\Delta v_o<0$. PCC-PT operates in period-n states with $\Delta v_o^H$ and $\Delta v_o^L$, rather than period-1 in the PWM switching converter [9]. Let the number of $P_H$ and $P_L$ in a control pulse repetition cycle be denoted as $\mu_H$ and $\mu_L$, respectively, then $\mu_H$ and $\mu_L$ satisfy $\mu_H/\mu_L=\Delta v_o^H/\Delta v_o^L$ [15], and the control pulse repetition cycle period $T_r$ is $T_r=(\mu_H+\mu_L)T$.

B. Operating Modes of PCC-PT Controlled Buck Converter

Let $i_{L\text{-}n}$ and $i_{L\text{-}n+1}$ denote the inductor currents at the beginning of the $n^{th}$ and $(n+1)^{th}$ switching cycle respectively. For inductor current $i_L$ of the PCC-PT controlled buck converter, there are four inductor current operation cases, as shown in Fig. 2.

Case 1: $i_{L\text{-}n}=0$ and $i_{L\text{-}n+1}=0$, as shown in Fig. 2(a);
Case 2: $i_{L\text{-}n} \neq 0$ and $i_{L\text{-}n+1}=0$, as shown in Fig. 2(b);
Case 3: $i_{L\text{-}n}=0$ and $i_{L\text{-}n+1} \neq 0$, as shown in Fig. 2(c);
Case 4: $i_{L\text{-}n} \neq 0$ and $i_{L\text{-}n+1} \neq 0$, as shown in Fig. 2(d).

Assume output voltage ripple is small enough to be ignored, that is, the output voltage can be considered as constant in a switching cycle. As $i_L=i_C+i_o$ and $i_o=\frac{v_o}{R}$, the peak inductor current $I_{L\text{-peak}}=I_{C\text{-peak}}+\frac{v_o}{R}$.

If $t_{\text{on}}+t_{\text{off}}<T_r$, $i_{L\text{-}n+1}=0$, which corresponds to Case 1 and 2, as shown in Fig. 2(a) and (b). In Cases 1 and 2, $i_L(t)$ in the $n^{th}$ switching cycle are

$$i_L(t)=i_{L\text{-}n}+\frac{(v_o-v_{ref})t}{L}, \quad [nT,nT+t_{\text{on}}]$$

$$i_L(t)=I_{L\text{-peak}}-\frac{v_o}{L}, \quad [nT+t_{\text{on}},nT+T_r-t_{\text{off}}]$$

Fig. 2: Different inductor current modes: (a) $i_{L\text{-}n}=0$ and $i_{L\text{-}n+1}=0$, (b) $i_{L\text{-}n} \neq 0$ and $i_{L\text{-}n+1}=0$, (c) $i_{L\text{-}n}=0$ and $i_{L\text{-}n+1} \neq 0$, and (d) $i_{L\text{-}n} \neq 0$ and $i_{L\text{-}n+1} \neq 0$. 
\[ i_L(t) = 0, \quad [nT + t_{on} + t_{off}, (n+1)T] \]

As \( i_L(t) = I_{\text{peak}} \), from (2), the time durations \( t_{on}, t_{off} \) and \( t_{off} \) of the PCC-PT controlled buck converter in Fig. 2(a) and (b) can be calculated as

\[ t_{on} = \frac{L(I_{\text{peak}} - i_{L,n} + v_o / R)}{v_{in} - v_o}, \quad (3a) \]
\[ t_{off} = \frac{L(I_{\text{peak}} + v_o / R)}{v_o}, \quad (3b) \]

\[ t_{off} = T - t_{on} - t_{off}. \quad (3c) \]

If \( t_{on} \) and \( t_{off} \) in Eq. (3) satisfy \( t_{on}+t_{off} > T, i_{L,n+1} > 0 \), which corresponds to Cases 3 and 4, as shown in Fig. 2(c) and (d). In Cases 3 and 4, in the \( n^{th} \) switching cycle, \( i_L(t) \) and the time durations \( t_{on} \) and \( t_{off} \) should be rewritten as

\[ i_L(t) = i_{L,n} + \frac{v_{in} - v_o}{L} t \quad [nT, nT + t_{on}] \quad (4a) \]
\[ i_L(t) = (I_{\text{peak}} + \frac{v_o}{R}) - \frac{v_o}{L} t \quad [nT + t_{on}, (n+1)T] \quad (4b) \]

\[ t_{on} = \frac{L(-i_{L,n} + I_{\text{peak}} + v_o / R)}{v_{in} - v_o}, \quad (4c) \]

\[ t_{off} = T - t_{on}. \quad (4d) \]

When \( t_{on} \) and \( t_{off} \) in Eq. (3) satisfy \( t_{on}+t_{off} = T, i_{L,n+1} = 0 \), there exists an inductor current boundary. From (3a) and (3b), such an inductor current boundary can be written as

\[ \frac{L(I_{\text{peak}} - i_{L,n} + v_o / R)}{v_{in} - v_o} + \frac{L(I_{\text{peak}} + v_o / R)}{v_o} - T = 0 \quad (5a) \]

Let \( R \) in (5a) be variable, and the right part of the equation in (5a) be \( f(R) \), then

\[ f(R) = (R(LI_{\text{peak}} + Iv_o - Rv_o t)v_{in} + (Rv_o T - Li_{L,n})v_o \]

\[ = 0 \quad (5b) \]

where \( f(R) = i_L(R) \) for the low power control pulse \( P_{L,L} \) and \( f(R) = i_H(R) \) for the high power control pulse \( P_{H,L} \). When \( f(R)<0, i_{L,n+1}<0 \); and when \( f(R)=0, i_{L,n+1}>0 \).

Thus, in a switching cycle, when \( i_{L,n}=0, f(R)<0 \), which correspond to Case 1 as shown in Fig. 2(a), means the converter operates in a DCM in this switching cycle; when \( i_{L,n} \neq 0, f(R)>0 \), which corresponds to Case 4, as shown in Fig. 2(d), means the converter operates in a CCM in this switching cycle.

As the PCC-PT controlled buck converter operates in period-\( n \) states rather than period-1, that is, control pulses \( P_{H,L} \) and \( P_{L,L} \) in \( n \) successive switching cycles constituting a control pulse repetition cycle, rather than period-1 in a PWM switching converter [9]. In a control pulse repetition cycle, the PCC-PT controlled buck converter may operate in DCM, CCM, and mixed DCM-CCM, herein mixed DCM-CCM is defined as the operating mode when both CCM and DCM exist in a control pulse repetition cycle. In mixed DCM-CCM, \( i_L \neq 0, f(R)<0 \) (corresponding to Case 2 as shown in Fig. 2(b)) and \( i_L=0, f(R)>0 \) (corresponding to Case 3 as shown in Fig. 2(c)) may occur. Thus, different from a PWM controlled buck converter which has two operating modes: DCM and CCM, the PCC-PT controlled buck converter has three operating modes: DCM, CCM and mixed DCM-CCM. When all switching cycles of a control pulse repetition cycle satisfy \( i_{L,n}=0, f_{H}(R)<0 \) and \( f_{L}(R)<0 \), the converter operates in DCM; when all switching cycles of a control pulse repetition cycle satisfy \( i_{L,n} \neq 0, f_{H}(R)>0 \) and \( f_{L}(R)>0 \), the converter operates in CCM; and when none of these conditions are satisfied, the converter operates in mixed DCM-CCM.

Fig. 3 shows the distributions of CCM, DCM and mixed DCM-CCM operating modes with the main circuit parameters as \( v_{in}=20V, v_{out}=5V, L=80\mu H, C=440\mu F \), and the controller parameters of the PCC-PT as \( T=50\mu s, T_{\text{peak}}^H=1.5A, T_{\text{peak}}^L=0.5A \). In Fig. 3, Line 1 is \( i_{L,n} \neq 0, f_{H}(R); \) Line 2 is \( i_{L,n}=0, f_{L}(R); \) Line 3 is \( i_{L,n} \neq 0, i_{L,n} \neq 0, f_{L}(R); \) and Line 4 is \( i_{L,n} = 0, f_{L}(R). \)

From Fig. 3, when \( R < 2.45 \Omega \), both lines 1 and 3 are above zero, that is, \( i_{L,n} \neq 0, i_{H}(R) > 0 \) and \( i_{H}(R) > 0 \), the converter operates in CCM. When \( R > 5.92 \Omega \), both lines 2 and 4 are below zero, that is, \( i_{L,n} = 0, f_{L}(R) < 0 \) and \( f_{H}(R) < 0 \), the converter operates in DCM. When \( 2.45 \Omega < R < 5.92 \Omega \), the converter operates in mixed DCM-CCM.

III. STEADY-STATE ANALYSIS

A. Output Voltage Variations of the PCC-PT Controlled Buck Converter

From the discussion in Section II, the PCC-PT controlled buck converter has four inductor current operation cases, the only difference between Case 1 (Case 3) and Case 2 (Case 4) is inductor current \( i_{L,n} \) at the beginning of switching cycle. When \( i_{L,n} = 0 \), Case 1 is the same as Case 2, and Case 3 is the same as Case 4. Thus, for convenience, only Cases 2 and 4 are analyzed in this section, and Cases 1 and 3 can be analyzed by considering \( i_{L,n} = 0 \).

1) Output Voltage Variation of Case 2 (Case 1)

As \( i_C = i_{L,n} \), from (2)

\[ i_C(t) = i_{C,n} + \frac{v_{in} - v_o}{L} t \quad [nT, nT + t_{on}], \quad (6a) \]
\[ i_C(t) = I_{\text{peak}} - \frac{v_o}{L} t \quad [nT + t_{on}, (n+1)T] \quad (6b) \]
\[ i_C(t) = \frac{v_o}{R} t \quad [nT + t_{on} + t_{off}, (n+1)T] \quad (6c) \]

where \( i_{C,n} = i_{L,n} - v_o/R \) is the capacitor current at the beginning.
output voltage variations $\Delta v_o^H$ and $\Delta v_o^L$ of the PCC-PT controlled buck converter operating in CCM and mixed DCM-CCM are shown in Fig. 4(b). In Fig. 4(b), solid lines show $\Delta v_o^H$ and $\Delta v_o^L$ for Case 4 when the converter operates in CCM, that is, $i_{c,n}=-v_o/R$, and dotted lines show $\Delta v_o^H$ and $\Delta v_o^L$ for Case 3 when the converter operates in mixed DCM-CCM, that is, $i_{c,n}=-v_o/R$.

When $2.45 \Omega < R < 5.92 \Omega$, the converter operates in mixed DCM-CCM. $\Delta v_o^H > 0$ and $\Delta v_o^L < 0$ are always satisfied as shown in Fig. 4(b). When $R < 2.45 \Omega$, the converter operates in CCM, with the decrease of $R$. $\Delta v_o^H$ decreases and $\Delta v_o^L$ increases slightly. When $R < 0.21 \Omega$, both $\Delta v_o^H$ and $\Delta v_o^L$ decrease dramatically. When $R > 0.21 \Omega$, $\Delta v_o^H < 0$, that is, even if $P_H$ is selected as the active control pulse, the output voltage cannot increase, and the PCC-PT controller cannot regulate the converter any more.

B. Circuit Parameter Design of the PCC-PT Controlled Buck Converter

From the previous discussion, for the PCC-PT controlled buck converter, when a high power control pulse $P_H$ is applied, the output voltage variation may be lower than zero, that is, $\Delta v_o^L > 0$ is not satisfied, and when a low power control pulse $P_L$ is applied, the output voltage variation may be larger than zero, that is, $\Delta v_o^H < 0$ is not satisfied. Thus, $\Delta v_o^H > 0$ and $\Delta v_o^L < 0$ should be considered in the parameter design. The design of control parameters follows.

For a light load condition, from (7), as $i_{c,n}=-v_o/R$, $\Delta v_o^L < 0$ and $\Delta v_o^H > 0$:

$$I_{C,peak}^L < \frac{2(v_o-v_{n})v_{o}^2T}{RLv_o} - \frac{v_o}{R}$$ (9a)

$$I_{C,peak}^H > \frac{2(v_o-v_{n})v_{o}^2T}{RLv_o} - \frac{v_o}{R}$$ (9b)

For a heavy load condition, from (8), as $\Delta v_o^L < 0$ and $\Delta v_o^H > 0$:

$$I_{C,peak}^L < 2\left[\frac{i_{c,n} + (v_o-v_{n})v_{o}^2T}{L} \right] \frac{v_o}{L}$$ (10a)

which can be rewritten as

$$I_{C,peak}^L < i_{c,n} + \frac{(v_o-v_{n})v_{o}^2T}{L} \left[ 1 + \frac{2L(v_o-Rv_o)v_{o}^2T}{Rv_o^2T} \right]$$ (10b)

To ensure $\Delta v_o^H > 0$, $i_{C,peak}$ should be smaller than the minimum of the right part of (10b), which occurs when $i_{c,n} = -v_o/R$.

$$I_{C,peak} < \frac{v_o}{L} + \frac{(v_o-v_{n})v_{o}^2T}{L}$$ (10c)

2) Output Voltage Variation of Case 4 (Case 3)

From (4) and (6), output voltage variation $\Delta v_o$ within one switching cycle is

$$\Delta v_o = \frac{-Lv_o}{2C(v_o-v_{n})} \left[ (v_o-I_{C,peak}^L-v_{n})^2 - v_o^2T^2 \right]$$ (8)

With the same circuit parameters as given in section II,
Thus, (9) and (10c) should be satisfied for the parameter design of the PCC-PT controlled buck converter.

C. Output Power Range

Base on the previous discussion, under a light load condition, the PCC-PT controlled buck converter operates in DCM. With increased load power, converter goes into mixed DCM-CCM, and then goes into CCM. Thus, the minimum and maximum load powers $P_{\text{min}}$ and $P_{\text{max}}$ occur in DCM and CCM, respectively.

When the converter operates in DCM, the power from the input power source is completely transferred to the load within one switching cycle. Assuming the converter is lossless, the power delivered from input power source to the load in one switching cycle is given by [9]

$$ P_{\text{DCM}} = v_i I_{\text{ave}} = \frac{L v_i}{2(v_m - v_o) T} \left( I_{C, \text{peak}} + \frac{v_o}{R} \right)^2 $$  \hspace{1cm} (11)

where $I_{\text{ave}}$ is the average current flowing through $S$ in a switching cycle. When $P_H$ is selected, $P_{\text{DCM}} = P_{\text{DCM}}^H$; and when $P_L$ is selected, $P_{\text{DCM}} = P_{\text{DCM}}^L$, that is

$$ P_{\text{DCM}}^H > P_o = \frac{v_o^2}{R}, $$ \hspace{1cm} (12)

$$ P_{\text{DCM}}^L \leq P_o = \frac{v_o^2}{R}, $$

where $P_o$ is load power.

When the converter operates in CCM, the inductor may store or release energy in one switching cycle, thus load power not only transferred from input power but also from the energy stored in the inductor. The input power $P_{\text{in}}$ in one switching cycle is

$$ P_{\text{in}} = v_{\text{in, ave}} I_{\text{ave}} = \frac{v_m}{2T} \left( I_{L, n+1} + I_{C, \text{peak}} \right) \frac{v_o}{R} \left( I_{L, n+1} - I_{C, \text{peak}} \right) $$  \hspace{1cm} (13)

From (2) and (4), $i_L, n+1$ can be obtained as $i_L, n+1 = I_{C, \text{peak}} + v_o/R - v_o(T - t_{on})/L$. The energy variation of the inductor $AE_L$ is

$$ AE_L = \frac{1}{2} L \left( I_{L, n+1}^2 - I_{C, \text{peak}}^2 \right) $$  \hspace{1cm} (14)

Then the power delivered from the input power source to the load in one switching cycle is

$$ P_{\text{CCM}} = P_{\text{in}} - \frac{AE_L}{T} $$  \hspace{1cm} (15)

With the same circuit parameters as given in section II, $P_{\text{DCM}}^H$, $P_{\text{DCM}}^L$, $P_{\text{CCM}}^H$, $P_{\text{CCM}}^L$ and $P_o$ with respect to $R$ are shown in Fig. 5. As shown in Fig. 5(a), all decrease with increased $R$. For $R > 5.92 \, \Omega$, the converter operates in DCM, as shown in Fig. 5(a).

For $R > 72.4 \, \Omega$, $P_{\text{DCM}}^L > P_o$, that is, when $P_L$ is selected as a control pulse, more power than load power $P_o$ is delivered from input power source to the load, which increases the output voltage rather than decreasing it. Thus, as with conventional PT control, $P_L$ of the PCC-PT controller determines the minimum load power $P_{\text{min}}$, which can be calculated from (12) as

$$ P_{\text{min}} = \frac{v_m^2}{2L} \left( \frac{v_m - v_o}{R} - \frac{v_o}{R} \right) $$  \hspace{1cm} (16)

For $5.92 \, \Omega < R < 72.4 \, \Omega$, as shown in Fig. 5(a), $P_{\text{DCM}}^L < P_o < P_{\text{DCM}}^H$, that is, in this condition, when $P_H$ is selected, more power than load power $P_o$ is delivered from the input power source to the load, which makes output voltage increase; and when $P_L$ is selected, less power than load power $P_o$ is delivered from the input power source to the load, which decreases the output voltage. Thus, PCC-PT control can adjust the buck converter output voltage by selecting $P_H$ or $P_L$.

For $2.45 \, \Omega < R < 5.92 \, \Omega$, the converter operates in mixed DCM-CCM, as shown in Fig. 5(a), both $P_{\text{DCM}}^L < P_o < P_{\text{DCM}}^H$ and $P_{\text{CCM}}^L < P_o < P_{\text{CCM}}^H$ are satisfied, that is, the PCC-PT controller can control the buck converter.

For $R < 2.45 \, \Omega$, the converter operates in CCM, as shown in Fig. 5(b), it always has $P_{\text{CCM}} < P_o < P_{\text{CCM}}^H$, thus, the converter can be controlled at heavy load conditions. Different from conventional PT control, the maximum load power of the PCC-PT controlled buck converter does not only depend on $P_H$, the output power can be high if the input power source can provide sufficient power.

From this analysis, as power delivered from the input power source to the load in one switching cycle increases (decreases) with the increase (decrease) of load power, the PCC-PT controlled buck converter can operate under a wide load power range.

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Fig. 5  The output powers of PCC-PT controlled buck converter: (a) the output power range of PCC-PT controlled buck converter and (b) zoom in view of (a).
which can be solved as
\[ \begin{align*}
\dot{v}_c(t) &= e^{-\alpha t}[v_{c,n} - v_c(t)] + k_1 \sin(\alpha t) + k_2 \cos(\alpha t) + k_3 v_c(t) + k_4 v_n(t), \\
\dot{i}_L(t) &= e^{-\alpha t}[i_{L,n} - i_L(t)] + \frac{R}{2(R + R_{ESR})} v_c(t) + \frac{1}{2(R + R_{ESR})} v_n(t).
\end{align*} \]  

where \( \alpha, k_1 \) and \( k_2 \) are
\[ \alpha = \frac{R R_{ESR} C + L}{2(R + R_{ESR}) L C} \omega, \quad \omega = \sqrt{\frac{R}{(R + R_{ESR}) L C} - \alpha^2}, \]
\[ k_1 = \frac{R}{(R + R_{ESR}) C \omega} i_{L,n} - \frac{R}{2(R + R_{ESR}) L C} v_n(t), \]
\[ k_2 = \frac{(L - R R_{ESR}) C \omega}{2(R + R_{ESR}) L C} i_{L,n} - \frac{R}{(R + R_{ESR}) L C} v_n(t). \]

As \( i_c(t_{on}) = I_{C, peak} \), from (18), the time duration \( t_{on} \) of switch state 1 is
\[ t_{on} = -\frac{\beta_2 + \sqrt{\beta_2^2 - 2\beta_1 \beta_3}}{\beta_1}, \]  

where
\[ \beta_1 = 2(\alpha^2 - \frac{R}{(R + R_{ESR}) L C}) (R i_{L,n} - v_{c,n}) - \alpha (R k_2 - k_1) \omega, \]
\[ \beta_2 = (R k_2 - k_1) \omega - \alpha (R i_{L,n} - v_{c,n}), \]  
\[ \beta_3 = (R i_{L,n} - v_{c,n}) - (R + R_{ESR}) I_{C, peak}. \]

After time duration \( t_{on} \), switch S is turned off and diode D is turned on, the converter operates in switch state 2. During this switch state, the inductor current \( i_L \) and capacitor voltage \( v_C \) are
\[ \begin{align*}
\text{L: } \frac{d i_L(t)}{d t} &= \frac{R}{R + R_{ESR}} v_C(t) - \frac{R R_{ESR}}{R + R_{ESR}} i_L(t), \\
\text{C: } \frac{d v_C(t)}{d t} &= \frac{R}{R + R_{ESR}} i_L(t) - \frac{1}{R + R_{ESR}} v_C(t).
\end{align*} \]  

which can be solved as
\[ \begin{align*}
\dot{v}_c(t) &= e^{-\alpha t}[v_{c,n} - v_c(t)] + k_1 \sin(\alpha t) + k_2 \cos(\alpha t) + k_3 v_c(t), \\
\dot{i}_L(t) &= e^{-\alpha t}[i_{L,n} - i_L(t)] + \frac{R}{2(R + R_{ESR}) L C} v_c(t) + \frac{1}{2(R + R_{ESR}) L C} v_n(t).
\end{align*} \]

where \( i_{L,n} \) and \( v_{C,n} \) are the initial conditions of switch state 2, \( v_c(t_{on}) \) can be obtained from (18), and \( k_1 \) and \( k_2 \) in (21) are
\[ \begin{align*}
k_1 &= \frac{R}{(R + R_{ESR}) C \omega} i_{L,n} - \frac{R}{2(R + R_{ESR}) L C} v_n(t), \\
k_2 &= \frac{(L - R R_{ESR}) C \omega}{2(R + R_{ESR}) L C} i_{L,n} - \frac{R}{(R + R_{ESR}) L C} v_n(t).
\end{align*} \]

In switch state 2, \( i_L \) decreases. When \( i_L \) decreases to zero before the end of the switching cycle, the converter operates in DCM, otherwise, it operates in CCM.

When the PCC-PT controlled buck converter operates in CCM, time duration \( t_{off} \) in this switch state is
\[ t_{off} = T - t_{on} \]  

When converter operates in DCM, as \( i_L(t_2) = 0 \), where \( t_2 = t_{on} + t_{off} \) from (21), the time duration \( t_{off} \) in this switch state is
\[ t_{off} = \frac{1}{\omega} \arctan \frac{R L_{C, peak} - v_c(t_{on})}{k_2 k_4} \]  

After \( i_L \) decreases to zero, it remains at zero, and both switch S and diode D are turned off. The converter operates in switch state 3. During this switch state, the inductor current \( i_L \) and
capacitor voltage $v_C$ are

$$\begin{align*}
& L \frac{di(t)}{dt} = 0, \\
& C \frac{dv(t)}{dt} = -\frac{1}{R + R_{ESR}} v_C(t).
\end{align*}$$

(24)

which can be solved as

$$\begin{align*}
& v_c(t) = e^{-\frac{t}{R + R_{ESR}}} v_c(t_i), \\
& i_l(t) = 0.
\end{align*}$$

(25)

where $v_c(t_i)$ is the initial condition of switch state 3, which can be obtained from (21) if $t_{off} = T - t_{on} - t_{off}$.

B. Discrete Iteration Model

From (18), (19), (21) and (22), the discrete iteration model of the PCC-PT controlled CCM buck converter can be derived as

$$\begin{align*}
& v_{C,n+1} = e^{-\alpha T} [(v_{C,n} - v_o) \cos \omega T + k_i \sin \omega T] \\
& + v_o \cos (\alpha T_{off}) + \frac{\omega}{\omega L} \sin (\alpha T_{off}) e^{-\alpha T}.
\end{align*}$$

(26)

$$\begin{align*}
& i_{L,n+1} = e^{-\alpha T} [(i_{L,n} - \frac{v_{C,n}}{R} \cos \omega T + k_i \sin \omega T] \\
& + \frac{v_o}{R} \cos (\alpha T_{off}) + \frac{\omega}{\omega L} \sin (\alpha T_{off}) e^{-\alpha T}.
\end{align*}$$

(27)

From (18), (19), (21), (23) and (25), the discrete iteration model of the PCC-PT controlled DCM buck converter is

$$\begin{align*}
& v_{C,n+1} = e^{-\alpha T} [v_{C,n} \cos \omega T \omega T_{off} + k_i \sin \omega T_{off}] \\
& + k_i \sin \alpha (\omega T_{on} + T_{off}) \\
& + v_o \cos (\alpha T_{off}) + \frac{\alpha}{\omega L} \sin (\alpha T_{off}) e^{-\alpha T}.
\end{align*}$$

special periodicities are presented. Fig. 7 (d) and (e) show bifurcation diagrams when the converter operates in DCM. The converter operates in period-3 with control pulse combination $1P_{hi}-2P_{li}$ for $14.93 \Omega < R < 15.08 \Omega$, and operates in period-2 with control pulse combination $1P_{hi}-1P_{li}$ for $8.62 \Omega < R < 8.81 \Omega$. Fig. 7 (f) shows bifurcation diagrams when the converter operates in mixed DCM-CCM. With the decrease of $R$, the converter operates in period-8 with control pulse combination $5P_{hi}-3P_{li}$, period-3 with control pulse combination $2P_{hi}-1P_{li}$, and period-7 with control pulse combination $5P_{hi}-2P_{li}$. The same control pulse combination, such as period-3 with control pulse combination $2P_{hi}-1P_{li}$, can exist in different operating modes of the PCC-PT controlled buck converter. Fig. 7 (g) shows bifurcation diagrams when the converter operates in CCM. The converter operates in period-4 with control pulse combination $3P_{hi}-1P_{li}$ for $1.12 \Omega < R < 1.61 \Omega$. From Fig. 7(d)-(g), with increased $R$, the ratio between the number of high power control pulse $\mu_{hi}$ and low power control pulse $\mu_{li}$ increases.

V. SIMULATION AND EXPERIMENTAL RESULTS

Fig. 8 shows simulation results of the PCC-PT controlled buck converter with the same circuit parameters as given in section II for different load resistances. Fig. 8(a) shows waveforms of output voltage $v_o$, capacitor current $i_C$, inductor
current $i_1$ and switch driving voltage $v_o$ for $R = 75 \, \Omega$. The load is too light to be controlled by the PCC-PT controller, $v_o$ is always higher than reference voltage $V_{ref}$, low power control pulse $P_1$ is thus continuously applied as the control pulse, and the converter operates in period-1 with the control pulse repetition cycle consisting of only $P_L$.

Fig. 8(b) and (c) show the waveforms for $R = 15 \, \Omega$ and $R = 8.7 \, \Omega$. The converter operates in DCM. For $R = 15 \, \Omega$, the converter operates in period-3 with control pulse combination $1P_{H}2P_{L}$. For $R = 8.7 \, \Omega$, converter operates in period-2 with control pulse combination $1P_{H}1P_{L}$.

Fig. 8(d)-(f) show the waveforms for $R = 5.1 \, \Omega$, $R = 4 \, \Omega$ and $R = 2.9 \, \Omega$. The converter operates in mixed DCM-CCM. For $R = 5.1 \, \Omega$, the converter operates in period-8 consisting of $5P_{H}$ and $3P_{L}$, and the control pulse combination is $2(2P_{H}1P_{L})-1(1P_{H}1P_{L})$. For $R = 4 \, \Omega$, the converter operates in period-3 with control pulse combination $2P_{H}1P_{L}$. For $R = 2.9 \, \Omega$, the converter operates in period-7 which consists of $5P_{H}$ and $2P_{L}$, and the control pulse combination is $1(3P_{H}1P_{L})-1(2P_{H}1P_{L})$.

Fig. 8(g)-(h) show the waveforms for $R = 1.5 \, \Omega$ and $R = 0.3 \, \Omega$. The converter operates in CCM. For $R = 1.5 \, \Omega$, the converter operates in period-4 with control pulse combination $3P_{H}1P_{L}$. For $R = 0.3 \, \Omega$, the converter operates in period-3 with control pulse combination $3P_{H}1P_{L}$. Simulation results of Fig. 8 are consistent with the theoretical analysis results.

Fig. 9 shows transient response of PCC-PT controlled buck converter under step load current variation from 5 A to 1 A and from 1 A to 5 A, respectively. As shown in Fig. 9(a), when load current $i_L$ step decreases at time $t=10.5 \, ms$, as inductor current $i_L$ can not change immediately, and because of $i_C=i_L-i_s$, output capacitor current $i_C$ abruptly jumps to $3.548 \, A$ which is larger than $I_{R \, \text{peak}}^{\text{H}}$, the switch $S$ is then turned off immediately. Three low power control pulses are selected as active control pulses to decrease the output voltage. After four switching cycles, the converter goes into a steady-state. The transient time is 4 switching cycles ($200 \, \mu s$) and the output voltage overshoot is $0.213 \, V$ (4.26%).

When load current $i_L$ step increases at time $t=10.5 \, ms$ as shown in Fig. 9(b), $i_C$ decreases to $-4.695 A$. Two high power control pulses are selected as active control pulses to increase the output voltage. After 2 switching cycles, the converter goes into a steady-state. The transient time is 2 switching cycles ($100 \, \mu s$) and the output voltage sag is $0.135 \, V$ (2.7%).

By using the same circuit parameters, experimental results of the PCC-PT controlled buck converters are shown in Fig. 10. For $R = 15 \, \Omega$, the converter operates in period-3 with control pulse combination $1P_{H}2P_{L}$, as shown in Fig. 10(a). For $R = 8.7 \, \Omega$, the converter operates in period-2 with control pulse combination $1P_{H}1P_{L}$, as shown in Fig. 10(b). As shown in Figs. 10(a) and (b), the converter operates in DCM.

Fig. 10(c) shows that for $R = 4 \, \Omega$, the converter operates in mixed DCM-CCM and in period-3 with control pulse combination $2P_{H}1P_{L}$. Fig. 10(d) shows that for $R = 0.3 \, \Omega$, the converter operates in CCM and in period-3 with control pulse combination $2P_{H}1P_{L}$. These experimental results verify the theoretical analysis and simulation results.
TABLE I. COMPARISON TABLE WITH THE PREVIOUS WORKS

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<tr>
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<tr>
<td>Input voltage ($v_{in}$)</td>
<td>20 V</td>
<td>12 V</td>
<td>20 V</td>
<td>20 V</td>
<td>15 V</td>
<td>12 V</td>
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<tr>
<td>Output voltage ($v_{o}$)</td>
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<td>12 V</td>
<td>5 V</td>
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<td>440 μF</td>
<td>1880 μF</td>
<td>800 μF</td>
<td>470 μF</td>
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<td>Switching frequency (f)</td>
<td>20 kHz</td>
<td>15 MHz (Maximum frequency)</td>
<td>20 kHz</td>
<td>16.7-66.7 kHz</td>
<td>20 kHz</td>
<td>40-125 kHz</td>
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<tr>
<td>Load range ($P_o$)</td>
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<td>2.5-6.25 W</td>
<td>6-12 W</td>
<td>0.5-4.9 W</td>
<td>6-13 W</td>
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</tr>
<tr>
<td>Operating modes</td>
<td>DCM, Mixed DCM-CCM, CCM</td>
<td>CCM</td>
<td>DCM</td>
<td>DCM</td>
<td>DCM</td>
<td>CCM</td>
</tr>
<tr>
<td>Line regulation</td>
<td>0.103% (20 V-300 V)</td>
<td>0.112% (20 V-300 V)</td>
<td>1.305% (0.5 A-1.25 A)</td>
<td>1.386% (0.08-0.8 A)</td>
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<tr>
<td>Load transient</td>
<td>1-5 A</td>
<td>6-18 A</td>
<td>1-2 A</td>
<td>1-2 A</td>
<td>0.08-0.8 A</td>
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<tr>
<td>Recovery time ($T_{recovery}$)</td>
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<td>38 μs</td>
<td>1.8 ms</td>
<td>125 μs</td>
<td>50 μs</td>
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<tr>
<td>Switching cycle number for recovery</td>
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<td>About 50 Switching cycles</td>
<td>9 Switching cycles</td>
<td>2-8 Switching cycles</td>
<td>1 Switching cycles</td>
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</tbody>
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Abbreviations: PCM-BF — Peak current mode bifrequency control; ICRIF — Inductor current ripple injection feedback circuit; IPR — Improved pulse regulation; VCM-PT — Valley current mode pulse train.

Fig. 10. Experimental results: (a) DCM, $R = 15 \, \Omega$, (b) DCM, $R = 8.7 \, \Omega$, (c) mixed DCM-CCM, $R = 4 \, \Omega$, and (d) CCM, $R = 0.3 \, \Omega$.

Fig. 11. Transient response experimental results of PT and PCC-PT controlled buck converter: (a) load current step decreases from 5 A to 1 A, and (b) load current step increases from 1 A to 5 A.

Fig. 11 shows the transient response experimental results of conventional PT and PCC-PT controlled buck converter under step load variation from 5 A to 1 A and from 1 A to 5 A, respectively. As shown in Fig. 11(a), when load current $i_o$ step decreases from 5 A to 1 A, output capacitor current $i_c$ increases to 3.2 A, which is larger than $i_{C\, peak}^H$, the switch S is then turned off immediately. Four low power control pulses are selected as active control pulses to decrease the output voltage. After five switching cycles, the converter goes into a steady-state. The transient response time is 5 switching cycles and the output voltage overshoot is about 0.2 V (4%). As shown in Fig. 11(b), when load current $i_o$ step increases from 1 A to 5 A, $i_c$ decreases to −2.8 A. One low power control pulse and one high power control pulse are selected as active control pulses to increase the output voltage. After 2 switching cycles, the converter goes into a steady-state. The transient response time is 2 switching cycles and the output voltage sag is 0.2 V (4%), approximately.

Moreover, the comparisons with the previous ripple-based control techniques are shown in Table I. From Table I, because of different switching frequencies f, the comparative study of transient responses of different control techniques is not obvious by comparing recovery times $T_{recovery}$. Thus, the switching cycle numbers of transient process, which reduces the effect of switching frequency, are considered to evaluate the transient performance. For PCC-PT controlled buck converter, only 2-5 switching cycles are required to get into steady state, which is less than the other control techniques. Moreover, the transient response of PCC-PT controlled converters can be improved by increasing switching frequency.

VI. CONCLUSION

In this paper, based on a discrete control technique, conventional PT control, for switching dc-dc converters, a PCC-PT control technique for the buck converter is proposed and analysed. Different from PT control, PCC-PT control uses peak capacitor current as a feedback control variable to generate high power control pulse $P_{Hi}$ and low power control pulse $P_{Li}$. The output voltage variations, $\Delta v_o^H$ and $\Delta v_o^L$, of the
PCC-PT controlled buck converter with output load variation are studied; from which, control parameter design is presented. From theory and simulation analysis, within a wide load range, $\Delta v_o^H > 0$ and $\Delta v_o^L < 0$ can always be satisfied, that is, the fast-scale oscillation in a conventional PT controlled buck converter can be eliminated. In order to better understand the characteristics of the PCC-PT control buck converter, an accurate discrete iteration model of the PCC-PT controlled buck converter was established. From this model, the effects of circuit parameters on stability performance of the PCC-PT controlled buck converter operating in DCM, mixed DCM-CCM, and CCM are studied. The presented simulation and experimental results verify the analysis.

REFERENCES


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